WM8950

ADC with Microphone Input and Programmable Digital Filters

DESCRIPTION

The WM8950 is a low power, high quality mono ADC designed for portable applications such as Digital Still Camera, Digital Voice Recorder or games console accessories.

The device integrates support for a differential or single ended mic. External component requirements are reduced as no separate microphone amplifiers are required.

Advanced Sigma Delta Converters are used along with digital decimation filters to give high quality audio at sample rates from 8 to 48ks/s. Additional digital filtering options are available, to cater for application filtering such as wind noise reduction, noise rejection, plus an advanced mixed signal ALC function with noise gate is provided.

An on-chip PLL is provided to generate the required Master Clock from an external reference clock. The PLL clock can also be output if required elsewhere in the system.

The WM8950 operates at supply voltages from 2.5 to 3.6V, although the digital supplies can operate at voltages down to 1.71V to save power. Different sections of the chip can also be powered down under software control by way of the selectable two or three wire control interface.

WM8950 is supplied in a very small 4x4mm QFN package, offering high levels of functionality in minimum board area, with high thermal performance.

FEATURES

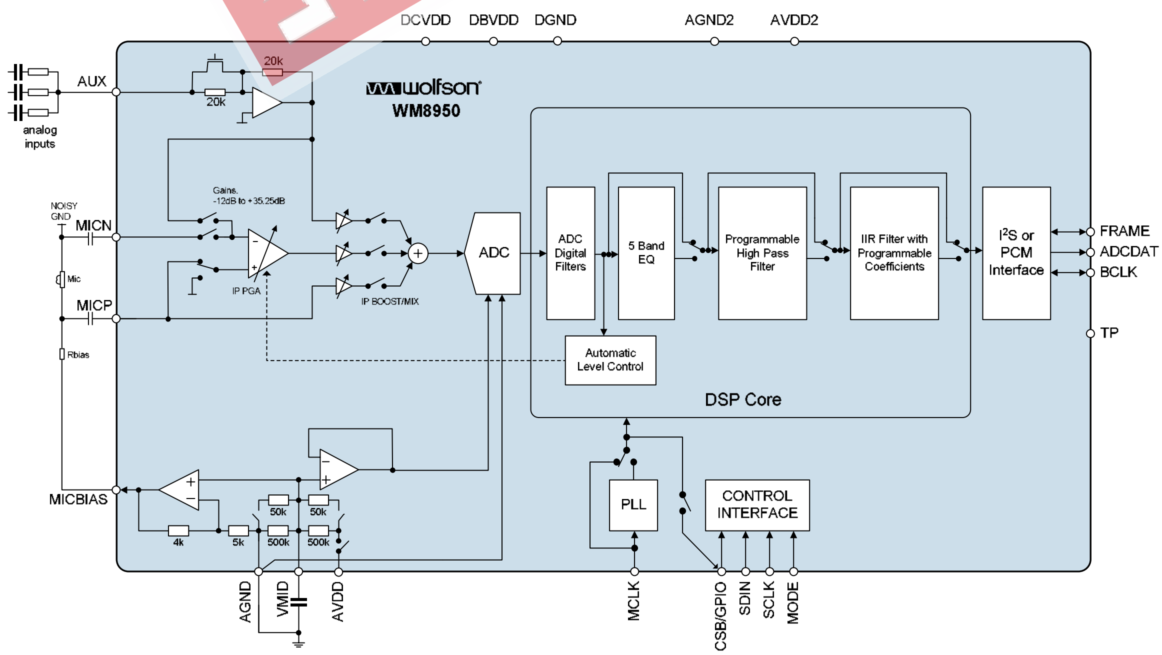
- **Mono ADC:**
- Audio sample rates:8, 11.025, 16, 22.05, 24, 32, 44.1, 48kHz
- SNR 95dB, THD -85dB ('A'-weighted @ 8 – 48ks/s)
- Multiple auxiliary analog inputs
- **Mic Preamps:**
- Differential or single end Microphone Interface
  - Programmable preamp gain
  - Psuedo differential inputs with common mode rejection
  - Programmable ALC / Noise Gate in ADC path
- Low-noise bias supplied for electret microphones

OTHER FEATURES

- 5 band EQ
- Programmable High Pass Filter (wind noise reduction)
- Fully Programmable IIR Filter (notch filter)
- On-chip PLL
- Low power, low voltage
  - 2.5V to 3.6V (digital: 1.71V to 3.6V)
  - power consumption TBD all-on 48ks/s mode
- 4x4x0.9mm 24 pin QFN package

APPLICATIONS

- Digital Still Camera
- General Purpose low power audio ADC
- Games console accessories
- Voice recorders



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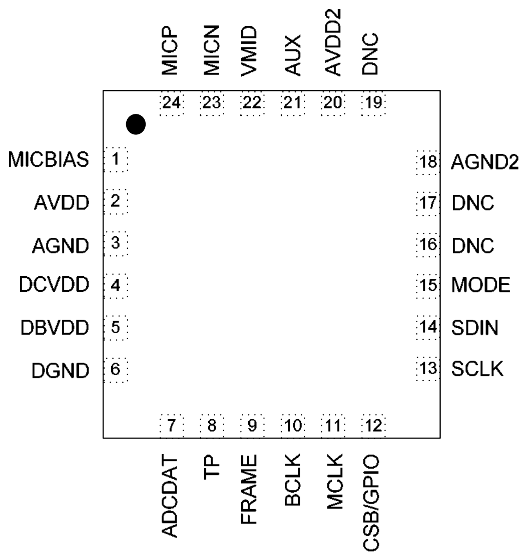


TOP VIEW

ORDERING INFORMATION

ORDER CODE	TEMPERATURE RANGE	PACKAGE	MOISTURE SENSITIVITY LEVEL	PACKAGE BODY TEMPERATURE
WM8950GEFL/V	-25°C to +85°C	24-pin QFN (4x4x0.9mm) (lead free)	MSL3	260°C
WM8950GEFL/RV	-25°C to +85°C	24-pin QFN (4x4x0.9mm) (lead free, tape and reel)	MSL3	260°C

Note:

Reel Quantity = 3,500

PIN DESCRIPTION

PIN NO	NAME	TYPE	DESCRIPTION
1	MICBIAS	Analogue Output	Microphone bias
2	AVDD	Supply	Analogue supply (feeds ADC)
3	AGND	Supply	Analogue ground (feeds ADC)
4	DCVDD	Supply	Digital core supply
5	DBVDD	Supply	Digital buffer (input/output) supply
6	DGND	Supply	Digital ground
7	ADCDAT	Digital Output	ADC digital audio data output
8	TP	Test Pin	Connect to ground
9	FRAME	Digital Input / Output	ADC sample rate clock or frame synch
10	BCLK	Digital Input / Output	Digital audio bit clock
11	MCLK	Digital Input	Master clock input
12	CSB/GPIO	Digital Input / Output	3-Wire MPU chip select or general purpose input/output pin.
13	SCLK	Digital Input	3-Wire MPU clock Input / 2-Wire MPU Clock Input
14	SDIN	Digital Input / Output	3-Wire MPU data Input / 2-Wire MPU Data Input
15	MODE	Digital Input	Control interface mode selection pin.
16	DNC	Do not connect	Leave this pin floating
17	DNC	Do not connect	Leave this pin floating
18	AGND2	Supply	Analogue ground
19	DNC	Do not connect	Leave this pin floating
20	AVDD2	Supply	Analogue supply
21	AUX	Analogue Input	Auxiliary analogue input
22	VMID	Reference	Decoupling for midrail reference voltage
23	MICN	Analogue Input	Microphone negative input
24	MICP	Analogue Input	Microphone positive input (common mode)

Note:

It is recommended that the QFN ground paddle should be connected to analogue ground on the application PCB.

ABSOLUTE MAXIMUM RATINGS

Absolute Maximum Ratings are stress ratings only. Permanent damage to the device may be caused by continuously operating at or beyond these limits. Device functional operating limits and guaranteed performance specifications are given under Electrical Characteristics at the test conditions specified.

ESD Sensitive Device. This device is manufactured on a CMOS process. It is therefore generically susceptible to damage from excessive static voltages. Proper ESD precautions must be taken during handling and storage of this device.

Wolfson tests its package types according to IPC/JEDEC J-STD-020B for Moisture Sensitivity to determine acceptable storage conditions prior to surface mount assembly. These levels are:

MSL1 = unlimited floor life at <30°C / 85% Relative Humidity. Not normally stored in moisture barrier bag.
MSL2 = out of bag storage for 1 year at <30°C / 60% Relative Humidity. Supplied in moisture barrier bag.
MSL3 = out of bag storage for 168 hours at <30°C / 60% Relative Humidity. Supplied in moisture barrier bag.

The Moisture Sensitivity Level for each package type is specified in Ordering Information.

CONDITION	MIN	MAX
DBVDD, DCVDD, AVDD, AVDD2 supply voltages	-0.3V	+4.2
Voltage range digital inputs	DGND -0.3V	DVDD +0.3V
Voltage range analogue inputs	AGND -0.3V	AVDD +0.3V
Operating temperature range, T_A	-25°C	+85°C
Storage temperature prior to soldering	30°C max / 85% RH max	
Storage temperature after soldering	-65°C	+150°C

Notes

1. Analogue and digital grounds must always be within 0.3V of each other.
2. All digital and analogue supplies are completely independent from each other.

RECOMMENDED OPERATING CONDITIONS

PARAMETER	SYMBOL	TEST CONDITIONS	MIN	TYP	MAX	UNIT
Digital supply range (Core)	DCVDD		1.71[1]		3.6	V
Digital supply range (Buffer)	DBVDD		1.71		3.6	V
Analogue supplies range	AVDD, AVDD2		2.5		3.6	V
Ground	DGND, AGND, AGND2			0		V

Notes

1. When using PLL, DCVDD must be 1.9V or higher.

ELECTRICAL CHARACTERISTICS

Test Conditions

DCVDD = 1.8V, AVDD = DBVDD = 3.3V, SPKVDD = 3.3V, T_A = +25°C, 1kHz signal, fs = 48kHz, 24-bit audio data unless otherwise stated.

PARAMETER	SYMBOL	TEST CONDITIONS	MIN	TYP	MAX	UNIT
Microphone Inputs (MICN, MICP)						
Full-scale Input Signal Level (Note 1) – note this changes with AVDD	V_{INFS}	PGABOOST = 0dB INPPGAVOL = 0dB		1.0 0		Vrms dBV
Mic PGA equivalent input noise	At 35.25dB gain			TBD		uV
Input resistance	R_{MICIN}	Gain set to 35.25dB		1.6		kΩ
Input resistance	R_{MICIN}	Gain set to 0dB		47		kΩ
Input resistance	R_{MICIN}	Gain set to -12dB		75		kΩ
Input resistance	R_{MICIP}	MICP2INPPGA = 1		94		kΩ
Input resistance	R_{MICIP}	MICP2INPPGA = 0		TBD		kΩ
Input Capacitance	C_{MICIN}			10		pF
Recommended coupling cap	C_{COUP}			220		pF
MIC Input Programmable Gain Amplifier (PGA)						
Programmable Gain			-12		35.25	dB
Programmable Gain Step Size		Guaranteed monotonic		0.75		dB
Mute Attenuation				TBD		dB
Selectable Input Gain Boost (0/+20dB)						
Gain Boost			0		20	dB
Automatic Level Control (ALC)/Limiter						
Target Record Level			-28.5		-6	dB
Programmable Gain			-12		35.25	dB
Programmable Gain Step Size		Guaranteed Monotonic		0.75		dB
Gain Hold Time (Note 2)	t_{HOLD}	MCLK=12.288MHz (Note 4)		0, 2.67, 5.33, 10.67, … , 43691 (time doubles with each step)		ms
Gain Ramp-Up (Decay) Time (Note 3)	t_{DCY}	ALCMODE=0 (ALC), MCLK=12.288MHz (Note 4)		3.3, 6.6, 13.1, … , 3360 (time doubles with each step)		ms
		ALCMODE=1 (limiter), MCLK=12.288MHz (Note 4)		0.73, 1.45, 2.91, … , 744 (time doubles with each step)		
Gain Ramp-Down (Attack) Time (Note 3)	t_{ATK}	ALCMODE=0 (ALC), MCLK=12.288MHz (Note 4)		0.83, 1.66, 3.33, … , 852 (time doubles with each step)		ms
		ALCMODE=1 (limiter), MCLK=12.288MHz (Note 4)		0.18, 0.36, 0.73, … , 186 (time doubles with each step)		
Mute Attenuation				TBD		dB
Analogue to Digital Converter (ADC)						
Signal to Noise Ratio (Note 5, 6)		A-weighted, 0dB gain		95		dB
Total Harmonic Distortion (Note 6)		full-scale, -1dB		-85		dB
Auxiliary Analogue Input (AUX)						
Full-scale Input Signal Level (0dB) – note this changes with AVDD	V_{INFS}			1.0 0		Vrms dBV
Input Resistance	R_{AUXIN}	AUXMODE=0		20		kΩ
Input Capacitance	C_{AUXIN}			10		pF

Test Conditions

DCVDD = 1.8V, AVDD = DBVDD = 3.3V, SPKVDD = 3.3V, T_A = +25°C, 1kHz signal, fs = 48kHz, 24-bit audio data unless otherwise stated.

PARAMETER	SYMBOL	TEST CONDITIONS	MIN	TYP	MAX	UNIT
Microphone Bias						
Bias Voltage (MBVSEL=0)	$V_{MICBIAS}$			0.9*AVDD		V
Bias Voltage (MBVSEL=1)	$V_{MICBIAS}$			0.75*AVDD		V
Bias Current Source	$I_{MICBIAS}$				3	mA
Output Noise Voltage	Vn	1K to 20kHz		15		nV/√Hz
Digital Input / Output						
Input HIGH Level	V_{IH}		0.7×DVDD			V
Input LOW Level	V_{IL}				0.3×DVDD	V
Output HIGH Level	V_{OH}	I_{OL}=1mA	0.9×DVDD			V
Output LOW Level	V_{OL}	I_{OH}-1mA			0.1xDVDD	V

TERMINOLOGY

1. MICN input only in single ended microphone configuration. Maximum input signal to MICP without distortion is -3dBV.
2. Hold Time is the length of time between a signal detected being too quiet and beginning to ramp up the gain. It does not apply to ramping down the gain when the signal is too loud, which happens without a delay.
3. Ramp-up and Ramp-Down times are defined as the time it takes for the PGA to change it's gain by 6dB.
4. All hold, ramp-up and ramp-down times scale proportionally with MCLK
5. Signal-to-noise ratio (dB) – SNR is a measure of the difference in level between the full scale output and the output with no signal applied. (No Auto-zero or Automute function is employed in achieving these results).
6. THD+N (dB) – THD+N is a ratio, of the rms values, of (Noise + Distortion)/Signal.

SIGNAL TIMING REQUIREMENTS

SYSTEM CLOCK TIMING

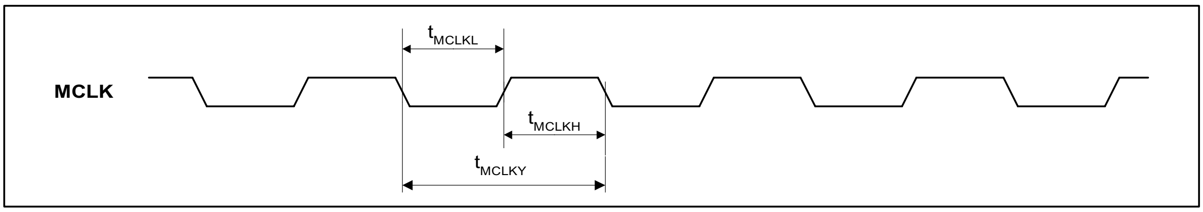


Figure 1 System Clock Timing Requirements

Test Conditions

DCVDD=1.8V, DBVDD=AVDD=SPKVDD=3.3V, DGND=AGND=SPKGND=0V, T_A = +25°C, Slave Mode fs = 48kHz, MCLK = 256fs, 24-bit data, unless otherwise stated.

PARAMETER	SYMBOL	MIN	TYP	MAX	UNIT
System Clock Timing Information					
MCLK System clock cycle time	T_{MCLKY}	Tbd			ns
MCLK duty cycle	T_{MCLKDS}	60:40		40:60	

AUDIO INTERFACE TIMING – MASTER MODE

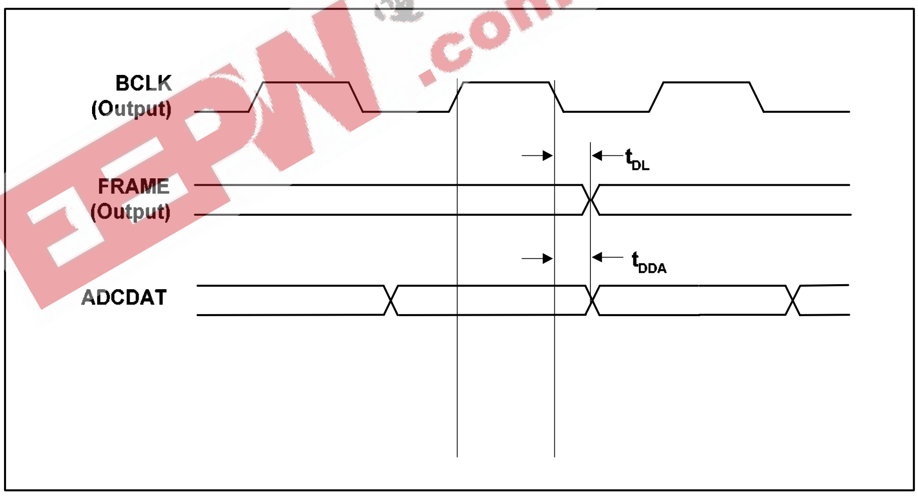


Figure 2 Digital Audio Data Timing – Master Mode (see Control Interface)

Test Conditions

DCVDD=1.8V, DBVDD=AVDD=SPKVDD=3.3V, DGND=AGND=SPKGND=0V, T_A=+25°C, Slave Mode, fs=48kHz, MCLK=256fs, 24-bit data, unless otherwise stated.

PARAMETER	SYMBOL	MIN	TYP	MAX	UNIT
Audio Data Input Timing Information					
FRAME propagation delay from BCLK falling edge	t_{DL}			10	ns
ADCDAT propagation delay from BCLK falling edge	t_{DDA}			10	ns

AUDIO INTERFACE TIMING – SLAVE MODE

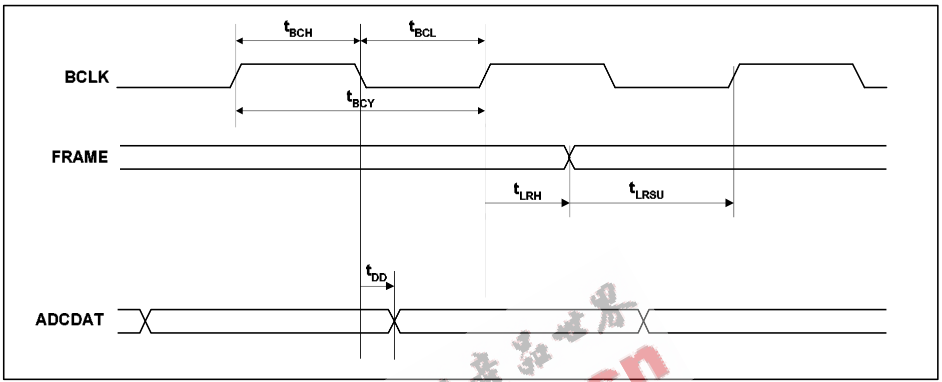


Figure 3 Digital Audio Data Timing – Slave Mode

Test Conditions

DCVDD=1.8V, DBVDD=AVDD=SPKVDD=3.3V, DGND=AGND=SPKGND=0V, T_A=+25°C, Slave Mode, fs=48kHz, MCLK= 256fs, 24-bit data, unless otherwise stated.

PARAMETER	SYMBOL	MIN	TYP	MAX	UNIT
Audio Data Input Timing Information					
BCLK cycle time	t_{BCY}	50			ns
BCLK pulse width high	t_{BCH}	20			ns
BCLK pulse width low	t_{BCL}	20			ns
FRAME set-up time to BCLK rising edge	t_{LRSU}	10			ns
FRAME hold time from BCLK rising edge	t_{LRH}	10			ns

Note:

BCLK period should always be greater than or equal to MCLK period.

CONTROL INTERFACE TIMING – 3-WIRE MODE

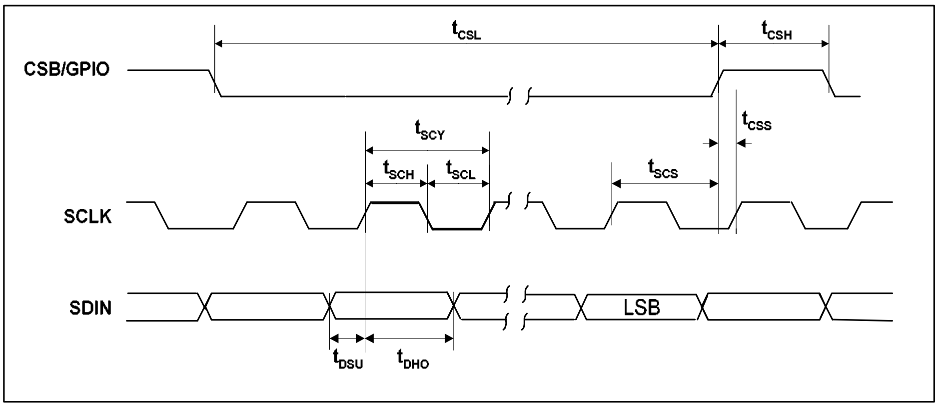


Figure 4 Control Interface Timing – 3-Wire Serial Control Mode

Test Conditions

DCVDD = 1.8V, DBVDD = AVDD = SPKVDD = 3.3V, DGND = AGND = SPKGND = 0V, T_A = +25°C, Slave Mode, fs = 48kHz, MCLK = 256fs, 24-bit data, unless otherwise stated.

PARAMETER	SYMBOL	MIN	TYP	MAX	UNIT
Program Register Input Information					
SCLK rising edge to CSB rising edge	t_{SCS}	80			ns
SCLK pulse cycle time	t_{SCY}	200			ns
SCLK pulse width low	t_{SCL}	80			ns
SCLK pulse width high	t_{SCH}	80			ns
SDIN to SCLK set-up time	t_{DSU}	40			ns
SCLK to SDIN hold time	t_{DHO}	40			ns
CSB pulse width low	t_{CSL}	40			ns
CSB pulse width high	t_{CSH}	40			ns
CSB rising to SCLK rising	t_{CSS}	40			ns
Pulse width of spikes that will be suppressed	t_{ps}	0		5	ns

CONTROL INTERFACE TIMING – 2-WIRE MODE

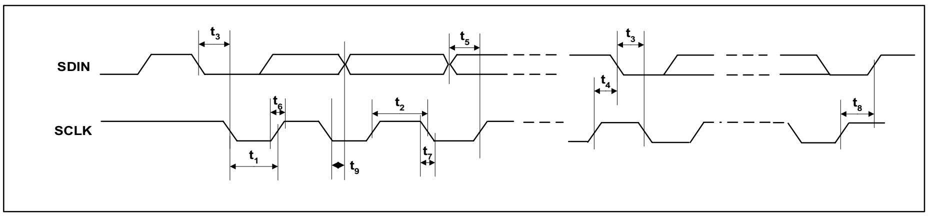


Figure 5 Control Interface Timing – 2-Wire Serial Control Mode

Test Conditions

DCVDD=1.8V, DBVDD=AVDD=SPKVDD=3.3V, DGND=AGND=SPKGND=0V, T_A = +25°C, Slave Mode, fs = 48kHz, MCLK = 256fs, 24-bit data, unless otherwise stated.

PARAMETER	SYMBOL	MIN	TYP	MAX	UNIT
Program Register Input Information					
SCLK Frequency		0		526	kHz
SCLK Low Pulse-Width	t_1	1.3			us
SCLK High Pulse-Width	t_2	600			ns
Hold Time (Start Condition)	t_3	600			ns
Setup Time (Start Condition)	t_4	600			ns
Data Setup Time	t_5	100			ns
SDIN, SCLK Rise Time	t_6			300	ns
SDIN, SCLK Fall Time	t_7			300	ns
Setup Time (Stop Condition)	t_8	600			ns
Data Hold Time	t_9			900	ns
Pulse width of spikes that will be suppressed	t_{ps}	0		5	ns

DEVICE DESCRIPTION

INTRODUCTION

The WM8950 is a low power audio ADC, with flexible line and microphone input. Applications for this device include games console accessories, digital still cameras, voice recorders and other general purpose audio applications.

FEATURES

The chip offers great flexibility in use, and so can support many different modes of operation as follows:

MICROPHONE INPUTS

Microphone inputs are provided, allowing for either a differential microphone input or a single ended microphone to be connected. These inputs have a user programmable gain range of -12dB to +35.25dB using internal resistors. After the input PGA stage comes a boost stage which can add a further 20dB of gain. A microphone bias is output from the chip which can be used to bias the microphones. The signal routing can be configured to allow manual adjustment of mic levels, or to allow the ALC loop to control the level of mic signal that is transmitted.

Total gain through the microphone paths of up to +55.25dB can be selected.

PGA AND ALC OPERATION

A programmable gain amplifier is provided in the input path to the ADC. This may be used manually or in conjunction with a mixed analogue/digital automatic level control (ALC) which keeps the recording volume constant.

AUX INPUT

The device includes a mono input, AUX, that can be used as an input for warning tones (beep) etc. This path can also be summed into the input in a flexible fashion, either to the input PGA as a second microphone input or as a line input. The configuration of this circuit, with integrated on-chip resistors allows several analogue signals to be summed into the single AUX input if required.

ADC

The mono ADC uses a multi-bit high-order oversampling architecture to deliver optimum performance with low power consumption. Various sample rates are supported, from the 8ks/s rate typically used in voice dictation, up to the 48ks/s rate used in high quality audio applications.

DIGITAL FILTERING

Advanced Sigma Delta Converters are used along with digital decimation and interpolation filters to give high quality audio at sample rates from 8ks/s to 48ks/s.

Application specific digital filters are also available which help to reduce the effect of specific noise sources such as 'wind noise'. The filters include a programmable ADC high pass filter, an IIR filter with fully programmable coefficients, and a 5-band equaliser that can be applied to the record path in order to improve the overall audio sound from the device.

AUDIO INTERFACES

The WM8950 has a standard audio interface, to support the transmission of audio data from the chip. This interface is a 4 wire standard audio interface which supports a number of audio data formats including I^2S, DSP Mode, MSB-First, left justified and MSB-First, right justified, and can operate in master or slave modes.

CONTROL INTERFACES

To allow full software control over all its features, the WM8950 offers a choice of 2 or 3 wire MPU control interface. It is fully compatible and an ideal partner for a wide range of industry standard microprocessors, controllers and DSPs. The selection between 2-wire mode and 3-wire mode is determined by the state of the MODE pin. If MODE is high then 3-wire control mode is selected, if MODE is low then 2-wire control mode is selected.

In 2 wire mode, only slave operation is supported, and the address of the device is fixed as 0011010.

CLOCKING SCHEMES

WM8950 offers the normal audio clocking scheme operation, where 256fs MCLK is provided to the ADC.

However, a PLL is also included which may be used to generate the internal master clock frequency in the event that this is not available from the system controller. This PLL uses an input clock, typically the 12MHz USB or ilink clock, to generate high quality audio clocks. If this PLL is not required for generation of these clocks, it can be reconfigured to generate alternative clocks which may then be output on the CSB/GPIO pin and used elsewhere in the system.

POWER CONTROL

The design of the WM8950 has given much attention to power consumption without compromising performance. It operates at low supply voltages, and includes the facility to power off any unused parts of the circuitry under software control, includes standby and power off modes.

INPUT SIGNAL PATH

The WM8950 has 3 flexible analogue inputs: two microphone inputs, and an auxiliary input. These inputs can be used in a variety of ways. The input signal path before the ADC has a flexible PGA block which then feeds into a gain boost/mixer stage.

MICROPHONE INPUTS

The WM8950 can accommodate a variety of microphone configurations including single ended and differential inputs. The inputs through the MICN, MICP and optionally AUX pins are amplified through the input PGA as shown in Figure 6 .

A pseudo differential input is the preferential configuration where the positive terminal of the input PGA is connected to the MICP input pin by setting MICP2INPPGA=1. The microphone ground should then be connected to MICN (when MICN2INPPGA=1) or optionally to AUX (when AUX2INPPGA=1) input pins.

Alternatively a single ended microphone can be connected to the MICN input with MICN2INPPGA set to 1. The non-inverting terminal of the input PGA should be connected internally to VMID by setting MICP2INPPGA to 0.

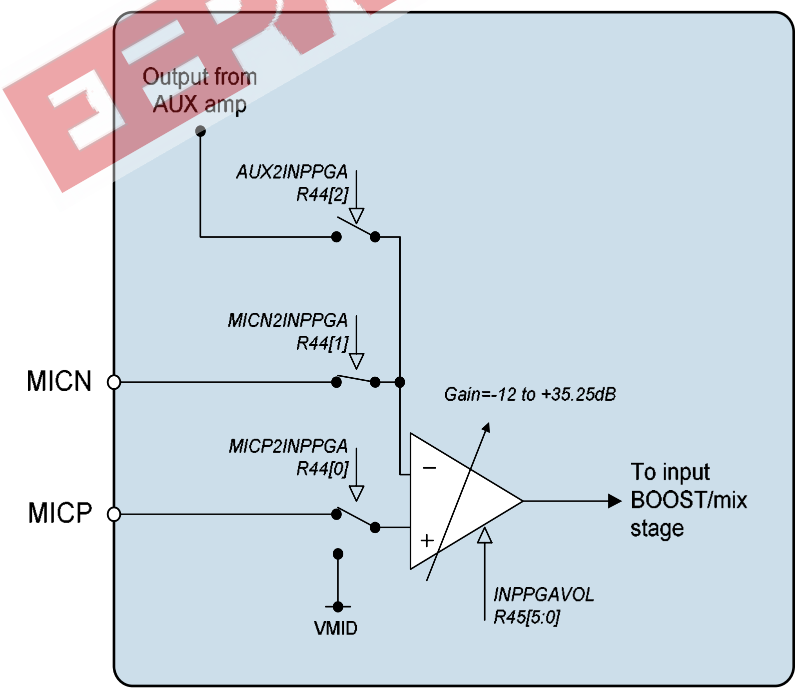


Figure 6 Microphone Input PGA Circuit (switch positions shown are for differential mic input)

REGISTER ADDRESS	BIT	LABEL	DEFAULT	DESCRIPTION
R44 Input Control	0	MICP2INPPGA	1	Connect input PGA amplifier positive terminal to MICP or VMID. 0 = input PGA amplifier positive terminal connected to VMID 1 = input PGA amplifier positive terminal connected to MICP through variable resistor string
	1	MICN2INPPGA	1	Connect MICN to input PGA negative terminal. 0=MICN not connected to input PGA 1=MICN connected to input PGA amplifier negative terminal.
	2	AUX2INPPGA	0	Select AUX amplifier output as input PGA signal source. 0=AUX not connected to input PGA 1=AUX connected to input PGA amplifier negative terminal.

The input PGA is enabled by the IPPGAEN register bit.

REGISTER ADDRESS	BIT	LABEL	DEFAULT	DESCRIPTION
R2 Power Management 2	2	INPPGAEN	0	Input microphone PGA enable 0 = disabled 1 = enabled

INPUT PGA VOLUME CONTROL

The input microphone PGA has a gain range from -12dB to +35.25dB in 0.75dB steps. The gain from the MICN input to the PGA output and from the AUX amplifier to the PGA output are always common and controlled by the register bits INPPGAVOL[5:0]. These register bits also affect the MICP pin when MICP2INPPGA=1.

When the Automatic Level Control (ALC) is enabled the input PGA gain is then controlled automatically and the INPPGAVOL bits should not be used.

REGISTER ADDRESS	BIT	LABEL	DEFAULT	DESCRIPTION
R45 Input PGA volume control	5:0	INPPGAVOL	010000	Input PGA volume 000000 = -12dB 000001 = -11.25db . 010000 = 0dB . 111111 = 35.25dB
	6	INPPGAMUTE	0	Mute control for input PGA: 0=Input PGA not muted, normal operation 1=Input PGA muted (and disconnected from the following input BOOST stage).
	7	INPPGAZC	0	Input PGA zero cross enable: 0=Update gain when gain register changes 1=Update gain on 1st zero cross after gain register write.
R32 ALC control 1	8	ALCSEL	0	ALC function select: 0=ALC off (PGA gain set by INPPGAVOL register bits) 1=ALC on (ALC controls PGA gain)

Table 1 Input PGA Volume Control

AUXILIARY INPUT

An auxiliary input circuit (Figure 7) is provided which consists of an amplifier which can be configured either as an inverting buffer for a single input signal or as a mixer/summer for multiple inputs with the use of external resistors. The circuit is enabled by the register bit AUXEN.

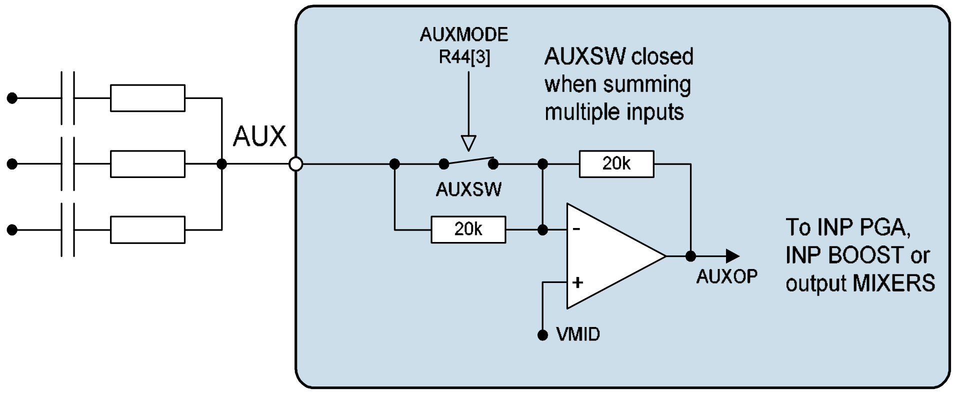


Figure 7 Auxiliary Input Circuit

The AUXMODE register bit controls the auxillary input mode of operation:

In buffer mode (AUXMODE=0) the switch labelled AUXSW in Figure 7 is open and the signal at the AUX pin will be buffered and inverted through the aux circuit using only the internal components.

In mixer mode (AUXMODE=1) the on-chip input resistor is bypassed, this allows the user to sum in multiple inputs with the use of external resistors. When used in this mode there will be gain variations through this path from part to part due to the variation of the internal 20kΩ resistors relative to the higher tolerance external resistors.

REGISTER ADDRESS	BIT	LABEL	DEFAULT	DESCRIPTION
R1 Power management 1	6	AUXEN	0	Auxiliary input buffer enable 0 = OFF 1 = ON
R44 Input control	3	AUXMODE	0	0 = inverting buffer 1 = mixer (on-chip input resistor bypassed)

Table 2 Auxiliary Input Buffer Control

INPUT BOOST

The input BOOST circuit has 3 selectable inputs: the input microphone PGA output, the AUX amplifier output and the MICP input pin (when not using a differential microphone configuration). These three inputs can be mixed together and have individual gain boost/adjust as shown in Figure 8.

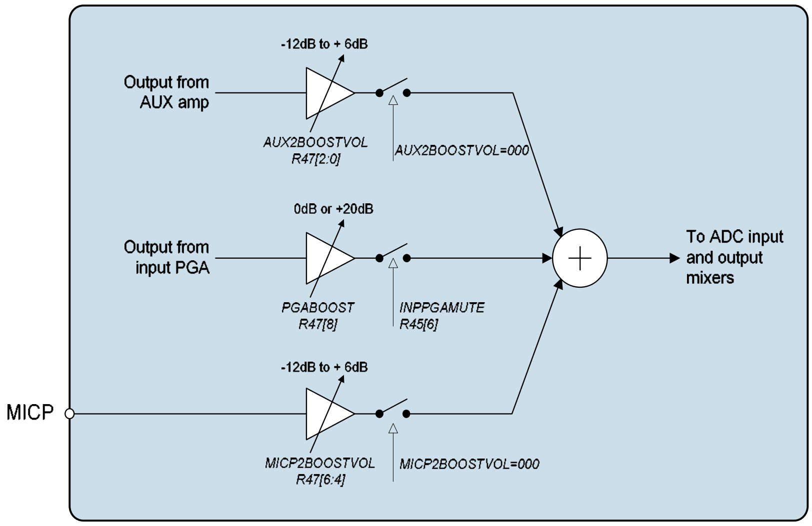


Figure 8 Input Boost Stage

The input PGA path can have a +20dB boost (PGABOOST=1) a 0dB pass through (PGABOOST=0) or be completely isolated from the input boost circuit (INPPGAMUTE=1).

REGISTER ADDRESS	BIT	LABEL	DEFAULT	DESCRIPTION
R45 Input PGA gain control	6	INPPGAMUTE	0	Mute control for input PGA: 0=Input PGA not muted, normal operation 1=Input PGA muted (and disconnected from the following input BOOST stage).
R47 Input BOOST control	8	PGABOOST	1	0 = PGA output has +0dB gain through input BOOST stage. 1 = PGA output has +20dB gain through input BOOST stage.

Table 3 Input BOOST Stage Control

The Auxiliary amplifier path to the BOOST stage is controlled by the AUX2BOOSTVOL[2:0] register bits. When AUX2BOOSTVOL=000 this path is completely disconnected from the BOOST stage. Settings 001 through to 111 control the gain in 3dB steps from -12dB to +6dB.

The MICP path to the BOOST stage is controlled by the MICP2BOOSTVOL[2:0] register bits. When MICP2BOOSTVOL=000 this input pin is completely disconnected from the BOOST stage. Settings 001 through to 111 control the gain in 3dB steps from -12dB to +6dB.

REGISTER ADDRESS	BIT	LABEL	DEFAULT	DESCRIPTION
R47 Input BOOST control	2:0	AUX2BOOSTVOL	000	Controls the auxiliary amplifer to the input boost stage: 000=Path disabled (disconnected) 001=-12dB gain through boost stage 010=-9dB gain through boost stage … 111=+6dB gain through boost stage
	6:4	MICP2BOOSTVOL	000	Controls the MICP pin to the input boost stage (NB, when using this path set MICPZIUNPPGA=0): 000=Path disabled (disconnected) 001=-12dB gain through boost stage 010=-9dB gain through boost stage … 111=+6dB gain through boost stage

Table 4 Input BOOST Stage Control

The BOOST stage is enabled under control of the BOOSTEN register bit.

REGISTER ADDRESS	BIT	LABEL	DEFAULT	DESCRIPTION
R2 Power management 2	4	BOOSTEN	0	Input BOOST enable 0 = Boost stage OFF 1 = Boost stage ON

Table 5 Input BOOST Enable Control

MICROPHONE BIASING CIRCUIT

The MICBIAS output provides a low noise reference voltage suitable for biasing electret type microphones and the associated external resistor biasing network. Refer to the Applications Information section for recommended external components. The MICBIAS voltage can be altered via the MBVSEL register bit. When MBVSEL=0, MICBIAS=0.9*AVDD and when MBVSEL=1, MICBIAS=0.75*AVDD. The output can be enabled or disabled using the MICBEN control bit.

REGISTER ADDRESS	BIT	LABEL	DEFAULT	DESCRIPTION
R1 Power management 1	4	MICBEN	0	Microphone Bias Enable 0 = OFF (high impedance output) 1 = ON

Table 6 Microphone Bias Enable

REGISTER ADDRESS	BIT	LABEL	DEFAULT	DESCRIPTION
R44 Input Control	8	MBVSEL	0	Microphone Bias Voltage Control 0 = 0.9 * AVDD 1 = 0.75 * AVDD

Table 7 Microphone Bias Voltage Control

The internal MICBIAS circuitry is shown in Figure 9. Note that the maximum source current capability for MICBIAS is 3mA. The external biasing resistors therefore must be large enough to limit the MICBIAS current to 3mA.

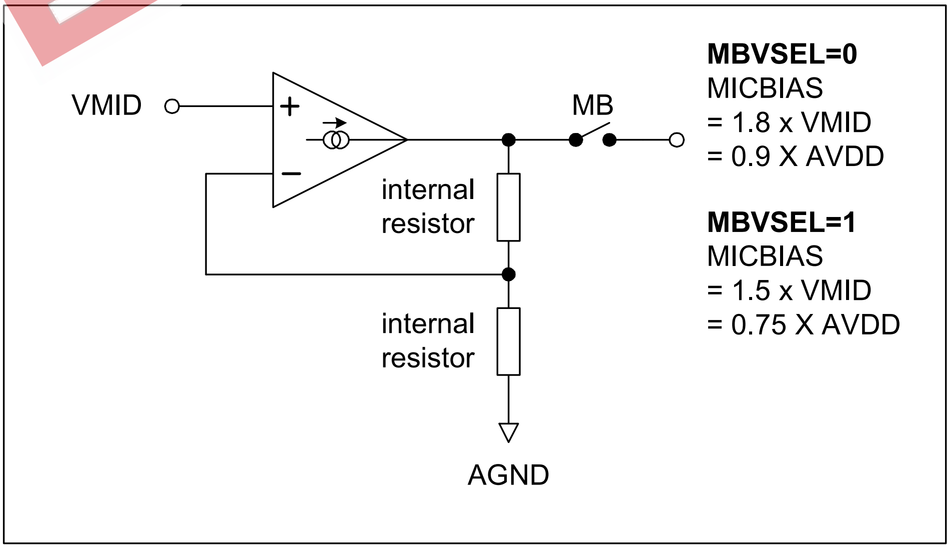


Figure 9 Microphone Bias Schematic

ANALOGUE TO DIGITAL CONVERTER (ADC)

The WM8950 uses a multi-bit, oversampled sigma-delta ADC channel. The use of multi-bit feedback and high oversampling rates reduces the effects of jitter and high frequency noise. The ADC Full Scale input level is proportional to AVDD. With a 3.3V supply voltage, the full scale level is 1.0V_{rms}. Any voltage greater than -1dBfs may overload the ADC and cause distortion.

ADC DIGITAL FILTERS

The ADC filters perform true 24 bit signal processing to convert the raw multi-bit oversampled data from the ADC to the correct sampling frequency to be output on the digital audio interface. The digital filter path is illustrated in Figure 10 .

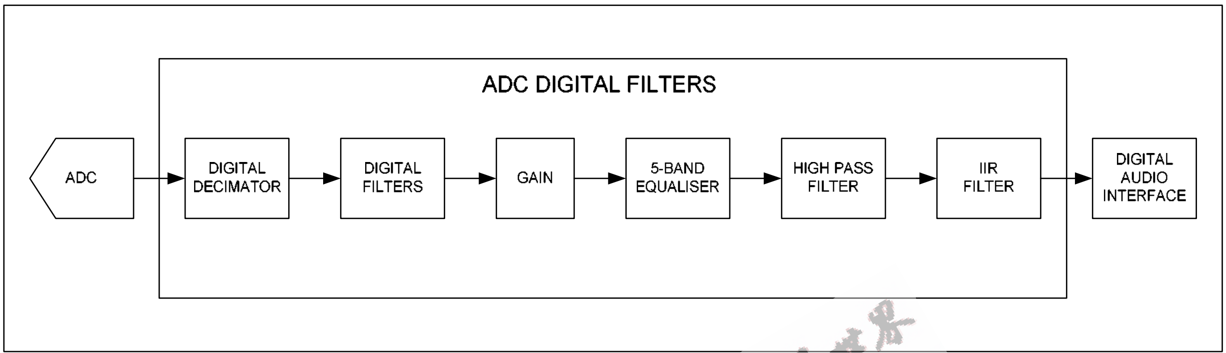


Figure 10 ADC Digital Filter Path

The ADC is enabled by the ADCEN register bit.

REGISTER ADDRESS	BIT	LABEL	DEFAULT	DESCRIPTION
R2 Power management 2	0	ADCEN	0	0 = ADC disabled 1 = ADC enabled

Table 8 ADC Enable

The polarity of the output signal can also be changed under software control using the ADCPOL register bit. The oversampling rate of the ADC can be adjusted using the ADCOSR register bit. With ADCOSR=0 the oversample rate is 64x which gives lowest power operation and when ADCOSR=1 the oversample rate is 128x which gives best performance.

REGISTER ADDRESS	BIT	LABEL	DEFAULT	DESCRIPTION
R14 ADC Control	3	ADCOSR	0	ADC oversample rate select: 0=64x (lower power) 1=128x (best performance)
	0	ADCPOL	0	0=normal 1=inverted

Table 9 ADC Oversample Rate Select

SELECTABLE HIGH PASS FILTER

A selectable high pass filter is provided. To disable this filter set HPFEN=0. The filter has two modes controlled by HPFAPP. In Audio Mode (HPFAPP=0) the filter is first order, with a cut-off frequency of 3.7Hz. In Application Mode (HPFAPP=1) the filter is second order, with a cut-off frequency selectable via the HPFCUT register. The cut-off frequencies when HPFAPP=1 are shown in Table 11.

REGISTER ADDRESS	BIT	LABEL	DEFAULT	DESCRIPTION
R14 ADC Control	8	HPFEN	1	High Pass Filter Enable 0=disabled 1=enabled
	7	HPFAPP	0	Select audio mode or application mode 0=Audio mode (1st order, fc = ~3.7Hz) 1=Application mode (2nd order, fc = HPFCUT)
	6:4	HPFCUT	000	Application mode cut-off frequency See Table 11 for details.

Table 10 ADC Filter Select

HPFCUT [2:0]	SAMPLE FREQUENCY (kHz)								
	8	11.025	12	16	22.05	24	32	44.1	48
	SR=101/100			SR=011/010			SR=001/000		
000	82	113	122	82	113	122	82	113	122
001	102	141	153	102	141	153	102	141	153
010	131	180	156	131	180	156	131	180	156
011	163	225	245	163	225	245	163	225	245
100	204	281	306	204	281	306	204	281	306
101	261	360	392	261	360	392	261	360	392
110	327	450	490	327	450	490	327	450	490
111	408	563	612	408	563	612	408	563	612

Table 11 High Pass Filter Cut-off Frequencies (HPFAPP=1) Values in Hz

Note that the High Pass filter values (when HPFAPP=1) work on the basis that the SR register bits are set correctly for the actual sample rate as shown in Table 11.

PROGRAMMABLE IIR FILTER

An IIR filter with fully programmable coefficients is provided, typically used as a notch filter for removing narrow band noise at a given frequency. This notch filter has a variable centre frequency and bandwidth, programmable via two coefficients, a0 and a1. a0 and a1 are represented by the register bits NFA0[13:0] and NFA1[13:0]. Because these coefficient values require four register writes to setup there is an NFU (Notch Filter Update) flag which should be set only when all four registers are setup.

REGISTER ADDRESS	BIT	LABEL	DEFAULT	DESCRIPTION
R27 Notch Filter 1	6:0	NFA0[13:7]	0	Notch Filter a0 coefficient, bits [13:7]
	7	NFEN	0	Notch filter enable: 0=Disabled 1=Enabled
	8	NFU	0	Notch filter update. The notch filter values used internally only update when one of the NFU bits is set high.
R28 Notch Filter 2	6:0	NFA0[6:0]	0	Notch Filter a0 coefficient, bits [6:0]
	8	NFU]	0	Notch filter update. The notch filter values used internally only update when one of the NFU bits is set high.
R29 Notch Filter 3	6:0	NFA1[13:7]	0	Notch Filter a1 coefficient, bits [13:7]
	8	NFU	0	Notch filter update. The notch filter values used internally only update when one of the NFU bits is set high.
R30 Notch Filter 4	6:0	NFA1[6:0]	0	Notch Filter a1 coefficient, bits [6:0]
	8	NFU	0	Notch filter update. The notch filter values used internally only update when one of the NFU bits is set high.

Table 12 Notch Filter Function

The coefficients are calculated as follows:

$$a_0 = \frac{1 - \tan(w_b / 2)}{1 + \tan(w_b / 2)}$$

$$a_1 = -(1 + a_0)\cos(w_0)$$

Where:

$$w_0 = 2\pi f_c / f_s$$

$$w_b = 2\pi f_b / f_s$$

f_c = centre frequency in Hz, f_b = -3dB bandwidth in Hz, f_s = sample frequency in Hz

The actual register values can be determined from the coefficients as follows:

NFA0 = -a0 x 2^{13}

NFA1 = -a1 x 2^{12}

DIGITAL ADC VOLUME CONTROL

The output of the ADCs can be digitally attenuated over a range from –127dB to 0dB in 0.5dB steps. The gain for a given eight-bit code X is given by:

Gain = 0.5 x (x–255) dB for 1 ≤ x ≤ 255, MUTE for x = 0

REGISTER ADDRESS	BIT	LABEL	DEFAULT	DESCRIPTION
R15 ADC Digital Volume	7:0	ADCVOL [7:0]	11111111 (0dB)	ADC Digital Volume Control 0000 0000 = Digital Mute 0000 0001 = -127dB 0000 0010 = -126.5dB ... 0.5dB steps up to 1111 1111 = 0dB

Table 13 ADC Volume

INPUT LIMITER / AUTOMATIC LEVEL CONTROL (ALC)

The WM8950 has an automatic pga gain control circuit, which can function as an input peak limiter or as an automatic level control (ALC).

In input peak limiter mode (ALCMODE bit = 1), a digital peak detector detects when the input signal goes above a predefined level and will ramp the pga gain down to prevent the signal becoming too large for the input range of the ADC. When the signal returns to a level below the threshold, the pga gain is slowly returned to its starting level. The peak limiter cannot increase the pga gain above its static level.

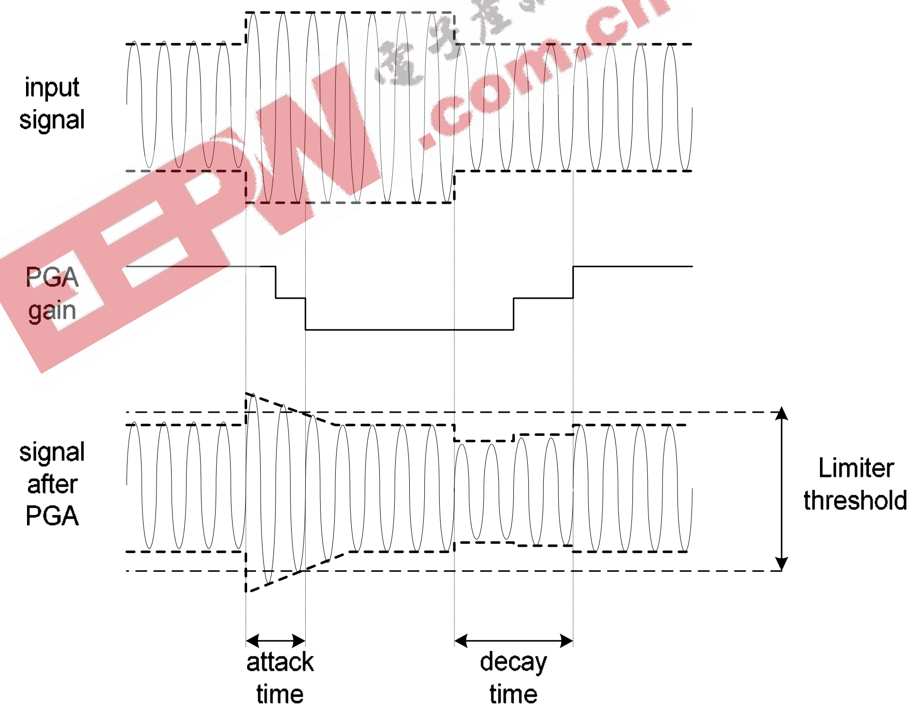


Figure 11 Input Peak Limiter Operation

In ALC mode (ALCMODE bit = 0) the circuit aims to keep a constant recording volume irrespective of the input signal level. This is achieved by continuously adjusting the PGA gain so that the signal level at the ADC input remains constant. A digital peak detector monitors the ADC output and changes the PGA gain if necessary.

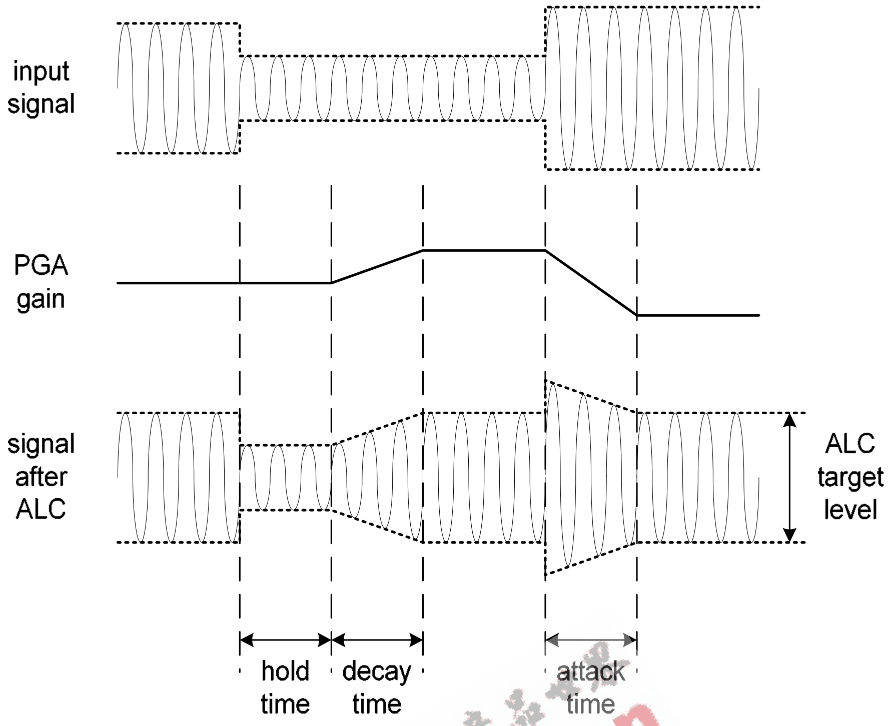


Figure 12 ALC Operation

The ALC/Limiter function is enabled by setting the register bit ALCSEL. When enabled, the recording volume can be programmed between –6dB and –28.5dB (relative to ADC full scale) using the ALCLVL register bits. An upper limit for the PGA gain can be imposed by setting the ALCMAX control bits and a lower limit for the PGA gain can be imposed by setting the ALCMIN control bits.

ALCHLD, ALCDCY and ALCATK control the hold, decay and attack times, respectively:

Hold time is the time delay between the peak level detected being below target and the PGA gain beginning to ramp up. It can be programmed in power-of-two (2^n) steps, e.g. 2.67ms, 5.33ms, 10.67ms etc. up to 43.7s. Alternatively, the hold time can also be set to zero. The hold time is not active in limiter mode (ALCMODE = 1). The hold time only applies to gain ramp-up, there is no delay before ramping the gain down when the signal level is above target.

Decay (Gain Ramp-Up) Time is the time that it takes for the PGA gain to ramp up and is given as a time per gain step, time per 6dB change and time to ramp up over 90% of it's range. The decay time can be programmed in power-of-two (2^n) steps, from 3.3ms/6dB, 6.6ms/6dB, 13.1ms/6dB, etc. to 3.36s/6dB.

Attack (Gain Ramp-Down) Time is the time that it takes for the PGA gain to ramp down and is given as a time per gain step, time per 6dB change and time to ramp down over 90% of it's range. The attack time can be programmed in power-of-two (2^n) steps, from 832us/6dB, 1.66ms/6dB, 3.328us/6dB, etc. to 852ms/6dB.

NB, In peak limiter mode the gain control circuit runs approximately 4x faster to allow reduction of fast peaks. Attack and Decay times for peak limiter mode are given below.

The hold, decay and attack times given in Table 14 are constant across sample rates so long as the SR bits are set correctly. E.g. when sampling at 48kHz the sample rates stated in Table 14 will only be correct if the SR bits are set to 000 (48kHz). If the actual sample rate was only 44.1kHz then the hold, decay and attack times would be scaled down by 44.1/48.

REGISTER ADDRESS	BIT	LABEL	DEFAULT	DESCRIPTION
R32 ALC Control 1	8	ALCSEL	0	ALC function select 0=ALC disabled 1=ALC enabled
	5:3	ALCMAXGAIN [2:0]	111 (+35.25dB)	Set Maximum Gain of PGA 111=+35.25dB 110=+29.25dB 101=+23.25dB 100=+17.25dB 011=+11.25dB 010=+5.25dB 001=-0.75dB 000=-6.75dB
	2:0	ALCMINGAIN [2:0]	000 (-12dB)	Set minimum gain of PGA 000=-12dB 001=-6dB 010=0dB 011=+6dB 100=+12dB 101=+18dB 110=+24dB 111=+30dB
R33 ALC Control 2	7:4	ALCHLD [3:0]	0000 (0ms)	ALC hold time before gain is increased. 0000 = 0ms 0001 = 2.67ms 0010 = 5.33ms … (time doubles with every step) 1111 = 43.691s
	3:0	ALCLVL [3:0]	1011 (-12dB)	ALC target – sets signal level at ADC input 0000 = -28.5dB FS 0001 = -27.0dB FS … (1.5dB steps) 1110 = -7.5dB FS 1111 = -6dB FS
	8	ALCZC	0 (zero cross off)	ALC uses zero cross detection circuit.

REGISTER ADDRESS	BIT	LABEL	DEFAULT	DESCRIPTION			
R34 ALC Control 3	8	ALCMODE	0	Determines the ALC mode of operation: 0=ALC mode 1=Limiter mode.			
	7:4	ALCDCY [3:0]	0011 (13ms/6dB)	Decay (gain ramp-up) time (ALCMODE =0)			
					Per step	Per 6dB	90% of range
				0000	410us	3.3ms	24ms
				0001	820us	6.6ms	48ms
				0010	1.64ms	13.1ms	192ms
				… (time doubles with every step)			
				1010 or higher	420ms	3.36s	24.576s
			0011 (2.9ms/6dB)	Decay (gain ramp-up) time (ALCMODE =1)			
					Per step	Per 6dB	90% of range
				0000	90.8us	726.4us	5.26ms
				0001	181.6us	1.453ms	10.53ms
				0010	363.2us	2.905ms	21.06ms
				… (time doubles with every step)			
				1010	93ms	744ms	5.39s
	3:0	ALCATK [3:0]	0010 (832us/6dB)	ALC attack (gain ramp-down) time (ALCMODE = 0)			
					Per step	Per 6dB	90% of range
				0000	104us	832us	6ms
				0001	208us	1.664ms	12ms
				0010	416us	3.328ms	24.1ms
				… (time doubles with every step)			
				1010 or higher	106ms	852ms	6.18s
			0010 (182us/6dB)	ALC attack (gain ramp-down) time (ALCMODE = 1)			
					Per step	Per 6dB	90% of range
				0000	22.7us	182.4us	1.31ms
				0001	45.4us	363.2us	2.62ms
				0010	90.8us	726.4us	5.26ms
				… (time doubles with every step)			
				1010	23.2ms	186ms	1.348s

Table 14 ALC Control Registers

ALC CLIP PROTECTION

To prevent clipping when a large signal occurs just after a period of quiet, the ALC circuit includes a clip protection function. If the ADC input signal exceeds 87.5% of full scale (–1.16dB), the PGA gain is ramped down at the maximum attack rate (as when ALCATK = 0000), until the signal level falls below 87.5% of full scale. This function is automatically enabled whenever the ALC is enabled.

Note:

If ATK = 0000, then the clip protection circuit makes no difference to the operation of the ALC. It is designed to prevent clipping when long attack times are used.

NOISE GATE

When the signal is very quiet and consists mainly of noise, the ALC function may cause "noise pumping", i.e. loud hissing noise during silence periods. The WM8950 has a noise gate function that prevents noise pumping by comparing the signal level at the input pins against a noise gate threshold, NGTH. The noise gate cuts in when:

Signal level at ADC [dB] < NGTH [dB] + PGA gain [dB] + Mic Boost gain [dB]

This is equivalent to:

Signal level at input pin [dB] < NGTH [dB]

The PGA gain is then held constant (preventing it from ramping up as it normally would when the signal is quiet).

The table below summarises the noise gate control register. The NGTH control bits set the noise gate threshold with respect to the ADC full-scale range. The threshold is adjusted in 6dB steps. Levels at the extremes of the range may cause inappropriate operation, so care should be taken with set–up of the function. Note that the noise gate only works in conjunction with the ALC function.

REGISTER ADDRESS	BIT	LABEL	DEFAULT	DESCRIPTION
R35 ALC Noise Gate Control	2:0	NGTH	000	Noise gate threshold: 000=-39dB 001=-45dB 010=-51db … (6dB steps) 111=-81dB
	3	NGATEN	0	Noise gate function enable 1 = enable 0 = disable

Table 15 ALC Noise Gate Control

GRAPHIC EQUALISER

A 5-band graphic EQ is provided, which can be applied to the ADC data under control of the EQMODE register bit.

REGISTER ADDRESS	BIT	LABEL	DEFAULT	DESCRIPTION
R18 EQ Control 1	8	EQMODE	1	0 = Equaliser applied to ADC data 1 = Equaliser bypassed

Table 16 EQ Select

The equaliser consists of low and high frequency shelving filters (Band 1 and 5) and three peak filters for the centre bands. Each has adjustable cut-off or centre frequency, and selectable boost (+/- 12dB in 1dB steps). The peak filters have selectable bandwidth.

REGISTER ADDRESS	BIT	LABEL	DEFAULT	DESCRIPTION
R18 EQ Band 1 Control	4:0	EQ1G	01100 (0dB)	Band 1 Gain Control. See Table 22 for details.
	6:5	EQ1C	01	Band 1 Cut-off Frequency: 00=80Hz 01=105Hz 10=135Hz 11=175Hz

Table 17 EQ Band 1 Control

REGISTER ADDRESS	BIT	LABEL	DEFAULT	DESCRIPTION
R19 EQ Band 2 Control	4:0	EQ2G	01100 (0dB)	Band 2 Gain Control. See Table 22 for details.
	6:5	EQ2C	01	Band 2 Centre Frequency: 00=230Hz 01=300Hz 10=385Hz 11=500Hz
	8	EQ2BW	0	Band 2 Bandwidth Control 0=narrow bandwidth 1=wide bandwidth

Table 18 EQ Band 2 Control

REGISTER ADDRESS	BIT	LABEL	DEFAULT	DESCRIPTION
R20 EQ Band 3 Control	4:0	EQ3G	01100 (0dB)	Band 3 Gain Control. See Table 22 for details.
	6:5	EQ3C	01	Band 3 Centre Frequency: 00=650Hz 01=850Hz 10=1.1kHz 11=1.4kHz
	8	EQ3BW	0	Band 3 Bandwidth Control 0=narrow bandwidth 1=wide bandwidth

Table 19 EQ Band 3 Control

REGISTER ADDRESS	BIT	LABEL	DEFAULT	DESCRIPTION
R21 EQ Band 4 Control	4:0	EQ4G	01100 (0dB)	Band 4 Gain Control. See Table 22 for details
	6:5	EQ4C	01	Band 4 Centre Frequency: 00=1.8kHz 01=2.4kHz 10=3.2kHz 11=4.1kHz
	8	EQ4BW	0	Band 4 Bandwidth Control 0=narrow bandwidth 1=wide bandwidth

Table 20 EQ Band 4 Control

REGISTER ADDRESS	BIT	LABEL	DEFAULT	DESCRIPTION
R22 EQ Band 5 Gain Control	4:0	EQ5G	01100 (0dB)	Band 5 Gain Control. See Table 22 for details.
	6:5	EQ5C	01	Band 5 Cut-off Frequency: 00=5.3kHz 01=6.9kHz 10=9kHz 11=11.7kHz

Table 21 EQ Band 5 Control

GAIN REGISTER	GAIN
00000	+12dB
00001	+11dB
00010	+10dB
…. (1dB steps)	
01100	0dB
01101	-1dB
11000 to 11111	-12dB

Table 22 Gain Register Table

A dedicated buffer is available for tieing off unused analogue input pins as shown below Figure 13. This buffer can be enabled using the BUFIOEN register bit.

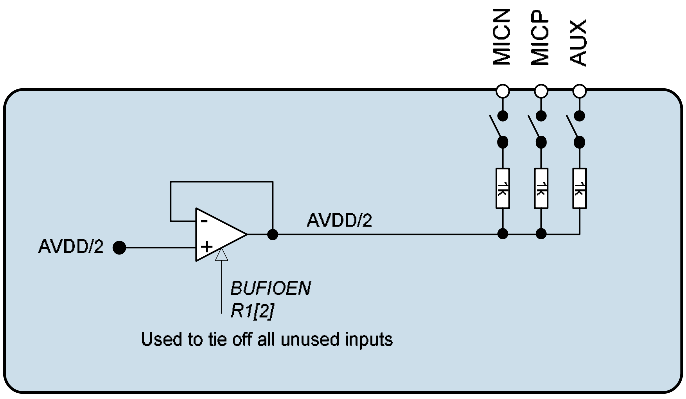


Figure 13 Unused Input Pin Tie-off Buffers

THERMAL SHUTDOWN

To protect the WM8950 from overheating a thermal shutdown circuit is included. If the device temperature reaches approximately 125^{0}C and the thermal shutdown circuit is enabled (TSDEN=1), an interrupt can be generated. See the GPIO and Interrupt Controller section for details.

REGISTER ADDRESS	BIT	LABEL	DEFAULT	DESCRIPTION
R49 Output control	1	TSDEN	1	Thermal Shutdown Enable 0 : thermal shutdown disabled 1 : thermal shutdown enabled

Table 23 Thermal Shutdown

DIGITAL AUDIO INTERFACES

The audio interface has three pins:

- ADCDAT: ADC data output
- FRAME: Data alignment clock
- BCLK: Bit clock, for synchronisation

The clock signals BCLK, and FRAME can be outputs when the WM8950 operates as a master, or inputs when it is a slave (see Master and Slave Mode Operation, below).

Five different audio data formats are supported:

- Left justified
- Right justified
- I^2S
- DSP mode early
- DSP mode late

All of these modes are MSB first. They are described in Audio Data Formats, below. Refer to the Electrical Characteristic section for timing information.

MASTER AND SLAVE MODE OPERATION

The WM8950 audio interface may be configured as either master or slave. As a master interface device the WM8950 generates BCLK and FRAME and thus controls sequencing of the data transfer on ADCDAT. To set the device to master mode register bit MS should be set high. In slave mode (MS=0), the WM8950 responds with data to clocks it receives over the digital audio interfaces.

AUDIO DATA FORMATS

In Left Justified mode, the MSB is available on the first rising edge of BCLK following an FRAME transition. The other bits up to the LSB are then transmitted in order. Depending on word length, BCLK frequency and sample rate, there may be unused BCLK cycles before each FRAME transition.

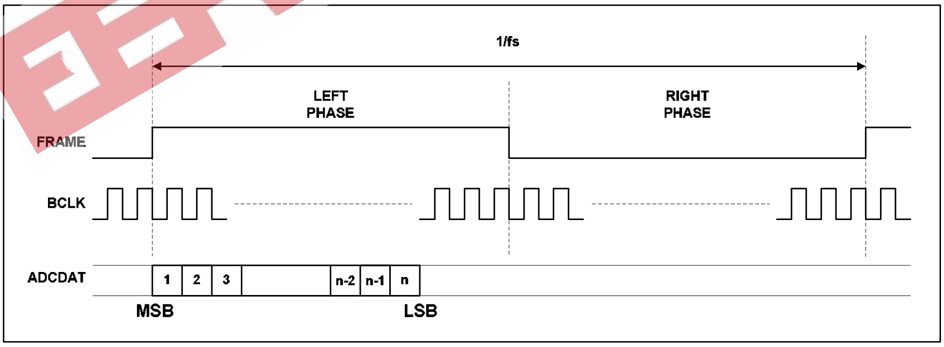


Figure 14 Left Justified Audio Interface (assuming n-bit word length)

In Right Justified mode, the LSB is available on the last rising edge of BCLK before a FRAME transition. All other bits are transmitted before (MSB first). Depending on word length, BCLK frequency and sample rate, there may be unused BCLK cycles after each FRAME transition.

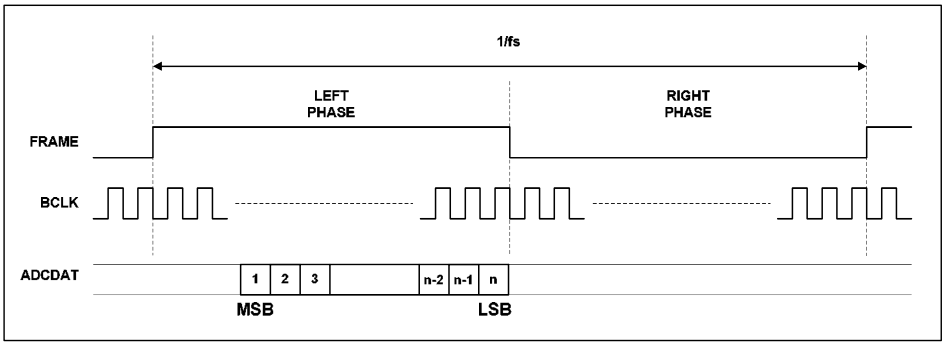


Figure 15 Right Justified Audio Interface (assuming n-bit word length)

In I²S mode, the MSB is available on the second rising edge of BCLK following a FRAME transition. The other bits up to the LSB are then transmitted in order. Depending on word length, BCLK frequency and sample rate, there may be unused BCLK cycles between the LSB of one sample and the MSB of the next.

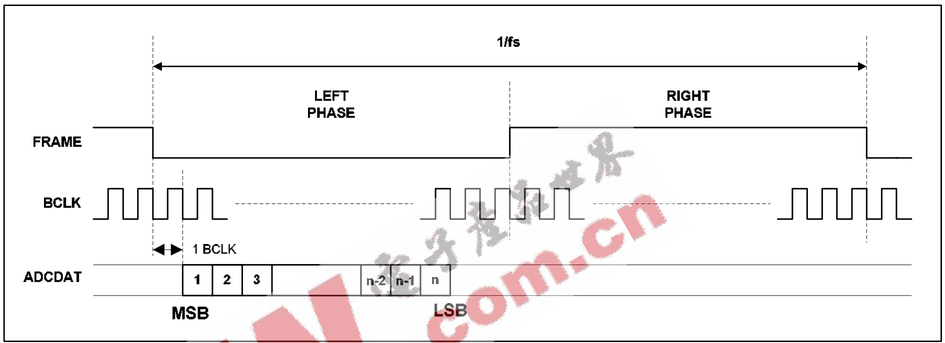


Figure 16 I²S Audio Interface (assuming n-bit word length)

In DSP/PCM mode, the left channel MSB is available on either the 1st (mode B) or 2nd (mode A) rising edge of BCLK (selectable by FRAMEP) following a rising edge of FRAME. Right channel data immediately follows left channel data. Depending on word length, BCLK frequency and sample rate, there may be unused BCLK cycles between the LSB of the right channel data and the next sample.

In device master mode, the LRC output will resemble the frame pulse shown in Figure 17 and Figure 18. In device slave mode, Figure 19 and Figure 20, it is possible to use any length of frame pulse less than 1/fs, providing the falling edge of the frame pulse occurs greater than one BCLK period before the rising edge of the next frame pulse.

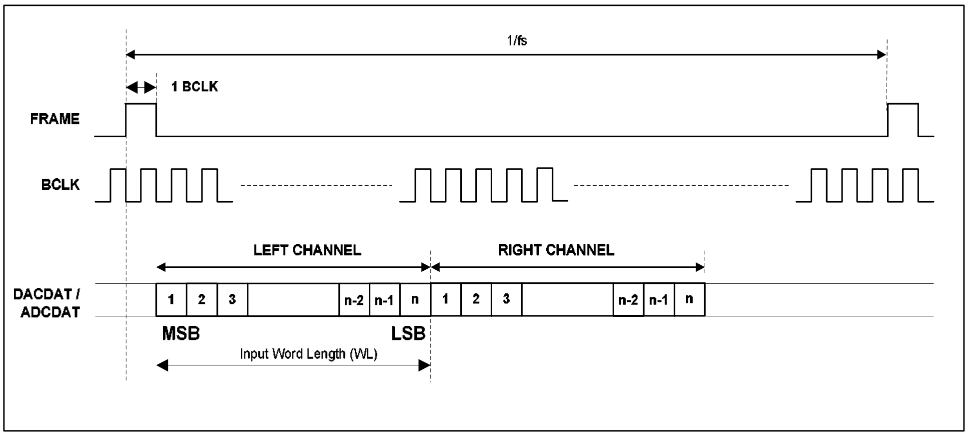


Figure 17 DSP/PCM Mode Audio Interface (mode A, LRP=0, Master)

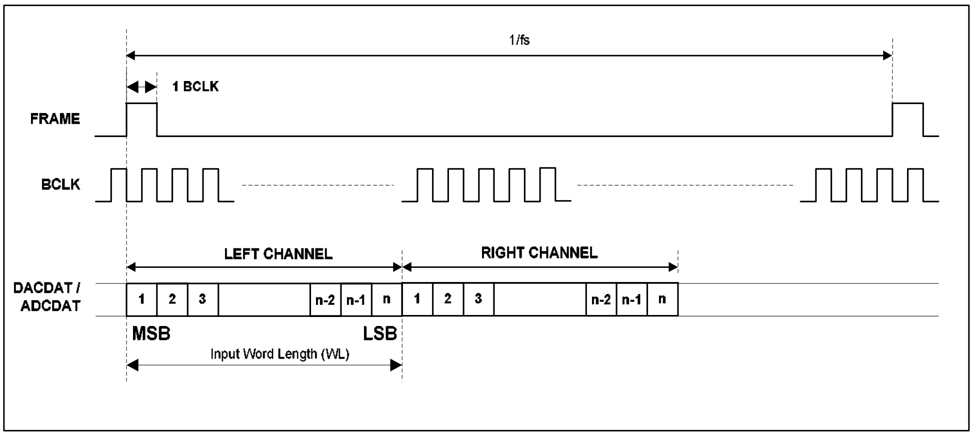


Figure 18 DSP/PCM Mode Audio Interface (mode B, LRP=1, Master)

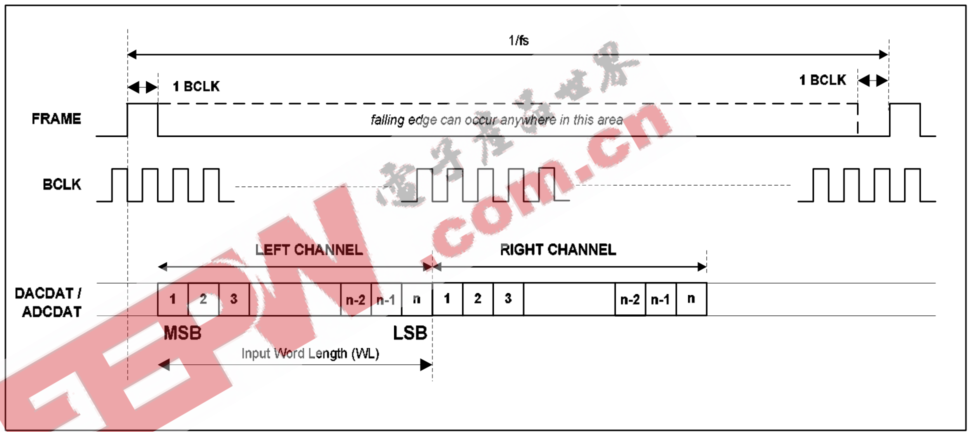


Figure 19 DSP/PCM Mode Audio Interface (mode A, LRP=0, Slave)

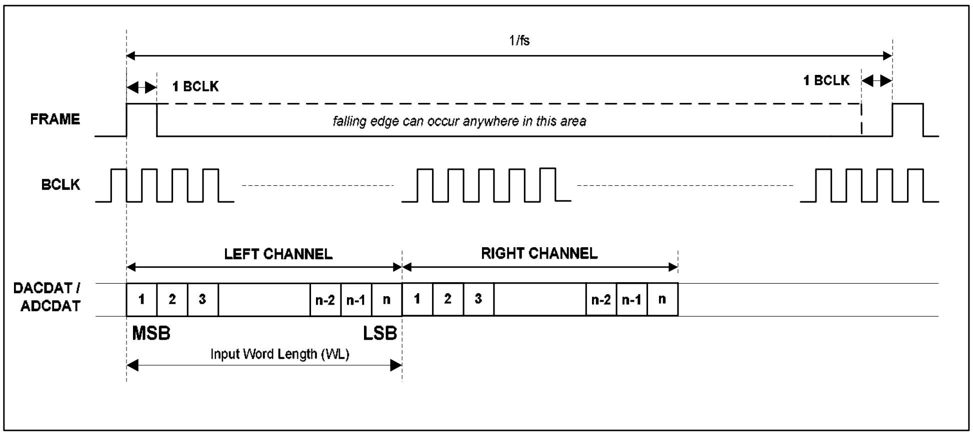


Figure 20 DSP/PCM Mode Audio Interface (mode B, LRP=0, Slave)

When using ADCLRSWAP = 1 in DSP/PCM mode, the data will appear in the Right Phase of the FRAME, which will be 16/20/24/32 bits after the FRAME pulse.

REGISTER ADDRESS	BIT	LABEL	DEFAULT	DESCRIPTION
R4 Audio interface control	1	ADCLRSWAP	0	Controls whether ADC data appears in 'right' or 'left' phases of FRAME clock: 0=ADC data appear in 'left' phase of FRAME 1=ADC data appears in 'right' phase of FRAME
	4:3	FMT	10	Audio interface Data Format Select: 00=Right Justified 01=Left Justified 10=I^{2}S format 11= DSP/PCM mode
	6:5	WL	10	Word length 00=16 bits 01=20 bits 10=24 bits 11=32 bits (see note)
	7	FRAMEP	0	Frame clock polarity 0=normal 1=inverted
				DSP Mode – mode A/B select 1 = MSB is available on 1st BCLK rising edge after FRAME rising edge (mode B) 0 = MSB is available on 2nd BCLK rising edge after FRAME rising edge (mode A)
	8	BCP	0	BCLK polarity 0=normal 1=inverted

Table 24 Audio Interface Control

AUDIO INTERFACE CONTROL

The register bits controlling audio format, word length and master / slave mode are summarised below. Each audio interface can be controlled individually.

Register bit MS selects audio interface operation in master or slave mode. In Master mode BCLK, and FRAME are outputs. The frequency of BCLK and FRAME in master mode are controlled with BCLKDIV. These are divided down versions of master clock. This may result in short BCLK pulses at the end of a frame if there is a non-integer ratio of BCLKs to FRAME clocks.

REGISTER ADDRESS	BIT	LABEL	DEFAULT	DESCRIPTION
R6 Clock generation control	0	MS	0	Sets the chip to be master over FRAME and BCLK 0=BCLK and FRAME clock are inputs 1=BCLK and FRAME clock are outputs generated by the WM8950 (MASTER)
	4:2	BCLKDIV	000	Configures the BCLK and FRAME output frequency, for use when the chip is master over BCLK. 000=divide by 1 (BCLK=MCLK) 001=divide by 2 (BCLK=MCLK/2) 010=divide by 4 011=divide by 8 100=divide by 16 101=divide by 32 110=reserved 111=reserved
	7:5	MCLKDIV	010	Sets the scaling for either the MCLK or PLL clock output (under control of CLKSEL) 000=divide by 1 001=divide by 1.5 010=divide by 2 011=divide by 3 100=divide by 4 101=divide by 6 110=divide by 8 111=divide by 12
	8	CLKSEL	1	Controls the source of the clock for all internal operation: 0=MCLK 1=PLL output

Table 25 Clock Control

COMPANDING

The WM8950 supports A-law and μ-law companding. Companding can be enabled on the ADC audio interface by writing the appropriate value to the ADC_COMP register bit.

REGISTER ADDRESS	BIT	LABEL	DEFAULT	DESCRIPTION
R5 Companding control	2:1	ADC_COMP	0	ADC companding 00=off 01=reserved 10=µ-law 11=A-law

Table 26 Companding Control

Companding involves using a piecewise linear approximation of the following equations (as set out by ITU-T G.711 standard) for data compression:

µ-law (where µ=255 for the U.S. and Japan):

$F(x) = \ln(1 + \mu|x|) / \ln(1 + \mu)$ -1 x 1

A-law (where A=87.6 for Europe):

$F(x) = A|x| / (1 + \ln A)$ } for x 1/A

$F(x) = (1 + \ln A|x|) / (1 + \ln A)$ } for 1/A x 1

The companded data is also inverted as recommended by the G.711 standard (all 8 bits are inverted for µ-law, all even data bits are inverted for A-law). The data will be transmitted as the first 8 MSB's of data.

Companding converts 13 bits (µ-law) or 12 bits (A-law) to 8 bits using non-linear quantization. The input data range is separated into 8 levels, allowing low amplitude signals better precision than that of high amplitude signals. This is to exploit the operation of the human auditory system, where louder sounds do not require as much resolution as quieter sounds. The companded signal is an 8-bit word containing sign (1-bit), exponent (3-bits) and mantissa (4-bits).

BIT8	BIT[7:4]	BIT[3:0]
SIGN	EXPONENT	MANTISSA

Table 27 8-bit Companded Word Composition

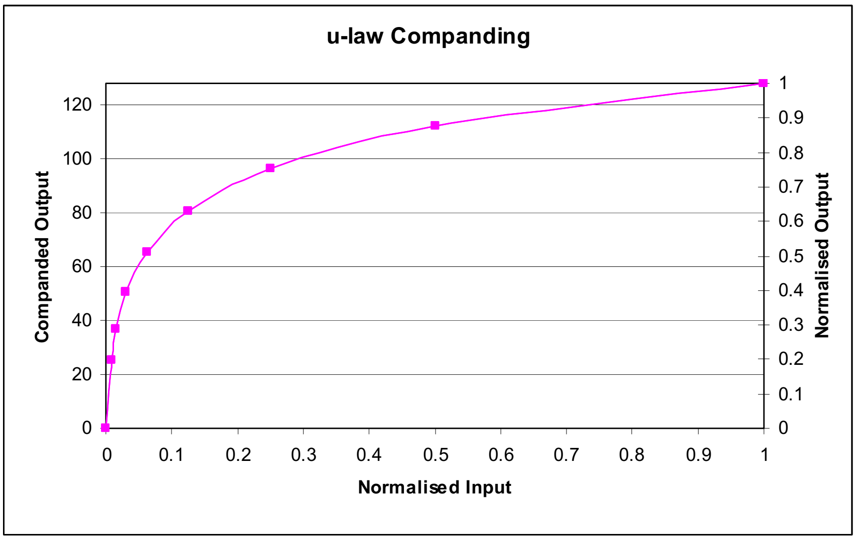


Figure 21 u-Law Companding

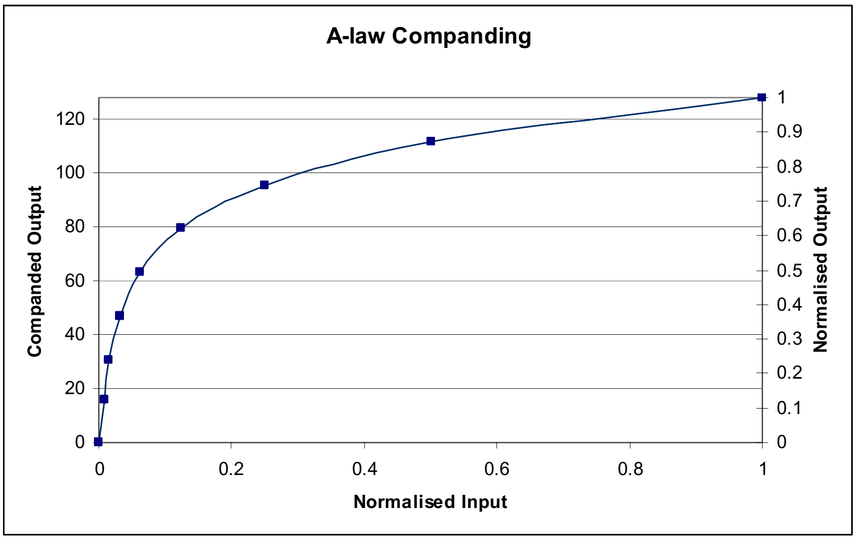


Figure 22 A-Law Companding

AUDIO SAMPLE RATES

The WM8950 sample rate for the ADC is set using the SR register bits. The cutoffs for the digital filters and the ALC attack/decay times stated are determined using these values and assume a 256fs master clock rate.

If a sample rate that is not explicitly supported by the SR register settings is required then the closest SR value to that sample rate should be chosen, the filter characteristics and the ALC attack, decay and hold times will scale appropriately.

REGISTER ADDRESS	BIT	LABEL	DEFAULT	DESCRIPTION
R7 Additional control	3:1	SR	000	Approximate sample rate (configures the coefficients for the internal digital filters): 000=48kHz 001=32kHz 010=24kHz 011=16kHz 100=12kHz 101=8kHz 110-111=reserved

Table 28 Sample Rate Control

MASTER CLOCK AND PHASE LOCKED LOOP (PLL)

The WM8950 has an on-chip phase-locked loop (PLL) circuit that can be used to:

Generate master clocks for the WM8950 audio functions from another external clock, e.g. in telecoms applications.

Generate and output (on pin CSB/GPIO) a clock for another part of the system that is derived from an existing audio master clock.

Figure 23 shows the PLL and internal clocking arrangment on the WM8950.

The PLL can be enabled or disabled by the PLLEN register bit.

REGISTER ADDRESS	BIT	LABEL	DEFAULT	DESCRIPTION
R1 Power management 1	5	PLLEN	0	PLL enable 0=PLL off 1=PLL on

Table 29 PLLEN Control Bit

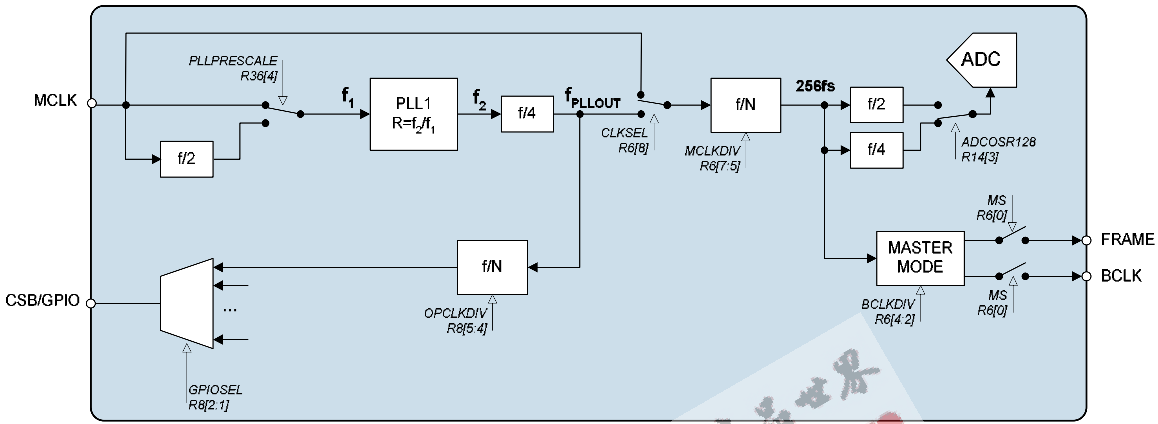


Figure 23 PLL and Clock Select Circuit

The PLL frequency ratio R = f_2/f_1 (see Figure 23) can be set using the register bits PLLK and PLLN:

PLLN = int R

PLLK = int (2^{24} (R-PLLN))

EXAMPLE:

MCLK=12MHz, required clock = 12.288MHz.

R should be chosen to ensure 5 < PLLN < 13. There is a fixed divide by 4 in the PLL and a selectable divide by N after the PLL which should be set to divide by 2 to meet this requirement.

Enabling the divide by 2 sets the required f_2 = 4 x 2 x 12.288MHz = 98.304MHz.

R = 98.304 / 12 = 8.192

PLLN = int R = 8

k = int (2^{24} x (8.192 – 8)) = 3221225 = 3126E9h

REGISTER ADDRESS	BIT	LABEL	DEFAULT	DESCRIPTION
R36 PLL N value	4	PLLPRESCALE	0	Divide MCLK by 2 before input to PLL
	3:0	PLLN	1000	Integer (N) part of PLL input/output frequency ratio. Use values greater than 5 and less than 13.
R37 PLL K value 1	5:0	PLLK [23:18]	0Ch	Fractional (K) part of PLL1 input/output frequency ratio (treat as one 24-digit binary number).
R38 PLL K Value 2	8:0	PLLK [17:9]	093h	
R39 PLL K Value 3	8:0	PLLK [8:0]	0E9h	

Table 30 PLL Frequency Ratio Control

The PLL performs best when f_2 is around 90MHz. Its stability peaks at N=8. Some example settings are shown in Table 31.

MCLK (MHz) (F1)	**DESIRED OUTPUT** (MHz)	**F2** (MHz)	**PRESCALE DIVIDE**	**POSTSCALE DIVIDE**	**R**	**N** (Hex)	**K** (Hex)
12	11.29	90.3168	1	2	7.5264	7	86C227
12	12.288	98.304	1	2	8.192	8	3126E9
13	11.29	90.3168	1	2	6.947446	6	F28BD5
13	12.288	98.304	1	2	7.561846	7	8FD526
14.4	11.29	90.3168	1	2	6.272	6	45A1CB
14.4	12.288	98.304	1	2	6.826667	6	D3A06D
19.2	11.29	90.3168	2	2	9.408	9	6872B0
19.2	12.288	98.304	2	2	10.24	A	3D70A4
19.68	11.29	90.3168	2	2	9.178537	9	2DB493
19.68	12.288	98.304	2	2	9.990243	9	FD80A0
19.8	11.29	90.3168	2	2	9.122909	9	1F76F8
19.8	12.288	98.304	2	2	9.929697	9	EE009F
24	11.29	90.3168	2	2	7.5264	7	86C227
24	12.288	98.304	2	2	8.192	8	3126E9
26	11.29	90.3168	2	2	6.947446	6	F28BD5
26	12.288	98.304	2	2	7.561846	7	8FD526
27	11.29	90.3168	2	2	6.690133	6	BOAC94
27	12.288	98.304	2	2	7.281778	7	482297

Table 31 PLL Frequency Examples

GENERAL PURPOSE INPUT/OUTPUT

The CSB/GPIO pin can be configured to perform a variety of useful tasks by setting the GPIOSEL register bits. The GPIO is only available in 2 wire mode.

REGISTER ADDRESS	**BIT**	**LABEL**	**DEFAULT**	**DESCRIPTION**
R8 GPIO control	2:0	GPIOSEL	000	CSB/GPIO pin function select: 000=CSB input 001=Reserved 010=Temp ok 011=Amute active 100=PLL clk o/p 101=PLL lock 110=Reserved 111=Reserved
	3	GPIOPOL	0	GPIO Polarity invert 0=Non inverted 1=Inverted
	5:4	OPCLKDIV	00	PLL Output clock division ratio 00=divide by 1 01=divide by 2 10=divide by 3 11=divide by 4

Table 32 CSB/GPIO Control

CONTROL INTERFACE

SELECTION OF CONTROL MODE AND 2-WIRE MODE ADDRESS

The control interface can operate as either a 3-wire or 2-wire MPU interface. The MODE pin determines the 2 or 3 wire mode as shown in Table 33.

The WM8950 is controlled by writing to registers through a serial control interface. A control word consists of 16 bits. The first 7 bits (B15 to B9) are address bits that select which control register is accessed. The remaining 9 bits (B8 to B0) are register bits, corresponding to the 9 bits in each control register.

MODE	INTERFACE FORMAT
Low	2 wire
High	3 wire

Table 33 Control Interface Mode Selection

3-WIRE SERIAL CONTROL MODE

In 3-wire mode, every rising edge of SCLK clocks in one data bit from the SDIN pin. A rising edge on CSB/GPIO latches in a complete control word consisting of the last 16 bits.

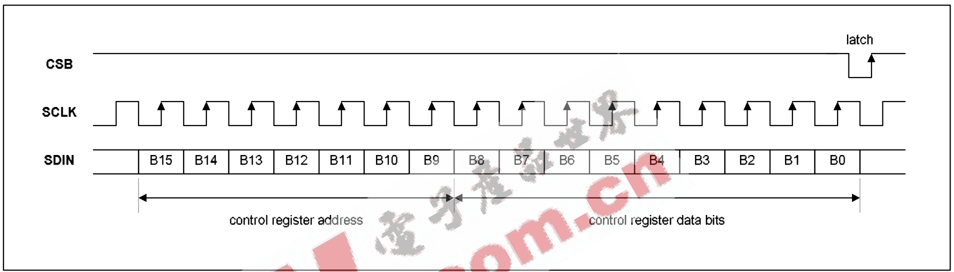


Figure 24 3-Wire Serial Control Interface

2-WIRE SERIAL CONTROL MODE

The WM8950 supports software control via a 2-wire serial bus. Many devices can be controlled by the same bus, and each device has a unique 7-bit device address (this is not the same as the 7-bit address of each register in the WM8950).

The WM8950 operates as a slave device only. The controller indicates the start of data transfer with a high to low transition on SDIN while SCLK remains high. This indicates that a device address and data will follow. All devices on the 2-wire bus respond to the start condition and shift in the next eight bits on SDIN (7-bit address + Read/Write bit, MSB first). If the device address received matches the address of the WM8950, then the WM8950 responds by pulling SDIN low on the next clock pulse (ACK). If the address is not recognised or the R/W bit is ‘1’ when operating in write only mode, the WM8950 returns to the idle condition and wait for a new start condition and valid address.

During a write, once the WM8950 has acknowledged a correct address, the controller sends the first byte of control data (B15 to B8, i.e. the WM8950 register address plus the first bit of register data). The WM8950 then acknowledges the first data byte by pulling SDIN low for one clock pulse. The controller then sends the second byte of control data (B7 to B0, i.e. the remaining 8 bits of register data), and the WM8950 acknowledges again by pulling SDIN low.

Transfers are complete when there is a low to high transition on SDIN while SCLK is high. After a complete sequence the WM8950 returns to the idle state and waits for another start condition. If a start or stop condition is detected out of sequence at any point during data transfer (i.e. SDIN changes while SCLK is high), the device jumps to the idle condition.

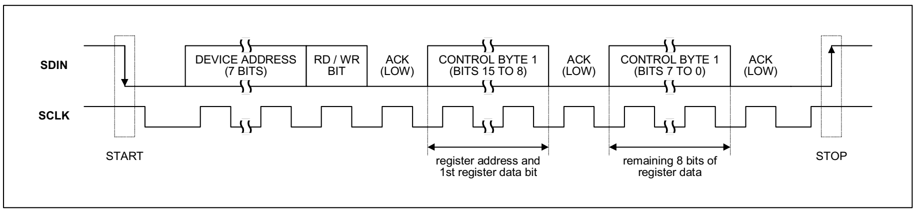


Figure 25 2-Wire Serial Control Interface

In 2-wire mode the WM8950 has a fixed device address, 0011010.

RESETTING THE CHIP

The WM8950 can be reset by performing a write of any value to the software reset register (address 0 hex). This will cause all register values to be reset to their default values. In addition to this there is a Power-On Reset (POR) circuit which ensures that the registers are set to default when the device is powered up.

POWER SUPPLIES

The WM8950 can use up to three separate power supplies:

AVDD, AVDD2, AGND and AGND2: Analogue supply, powers all analogue functions. AVDD can range from 2.5V to 3.6V and has the most significant impact on overall power consumption. A large AVDD slightly improves audio quality.

DCVDD: Digital core supply, powers all digital functions except the audio and control interfaces. DCVDD can range from 1.71V to 3.6V, and has no effect on audio quality. The return path for DCVDD is DGND, which is shared with DBVDD.

DBVDD Can range from 1.71V to 3.6V. DBVDD return path is through DGND.

It is possible to use the same supply voltage for all supplies. However, digital and analogue supplies should be routed and decoupled separately on the PCB to keep digital switching noise out of the analogue signal paths.

POWER MANAGEMENT

SAVING POWER BY REDUCING OVERSAMPLING RATE

The default mode of operation of the ADC digital filters is in 64x oversampling mode. Under the control of ADCOSR the oversampling rate may be doubled. 64x oversampling results in a slight decrease in noise performance compared to 128x but lowers the power consumption of the device.

REGISTER ADDRESS	BIT	LABEL	DEFAULT	DESCRIPTION
R14 ADC control	3	ADCOSR128	0	ADC oversample rate select 0 = 64x (lowest power) 1 = 128x (best SNR)

Table 34 ADC Oversampling Rate Selection

VMID

The analogue circuitry will not work unless VMID is enabled (VMIDSEL 00). The impedance of the VMID resistor string, together with the decoupling capacitor on the VMID pin will determine the startup time of the VMID circuit.

REGISTER ADDRESS	BIT	LABEL	DEFAULT	DESCRIPTION
R1 Power management 1	1:0	VMIDSEL	00	Reference string impedance to VMID pin (detemines startup time): 00=off (open circuit) 01=75kΩ 10=300kΩ 11=2.5kΩ (for fastest startup)

Table 35 VMID Impedance Control

BIASEN

REGISTER ADDRESS	BIT	LABEL	DEFAULT	DESCRIPTION
R1 Power management 1	3	BIASEN	0	Analogue amplifier bias control

Table 36 BIASEN Control

ESTIMATED SUPPLY CURRENTS

When the ADC is enabled it is estimated that approximately 4mA will be drawn from DCVDD when fs=48kHz (This will be lower at lower sample rates). When the PLL is enabled an additional 700 microamps will be drawn from DCVDD.

Table 59 shows the estimated 3.3V AVDD current drawn by various circuits, by register bit.

REGISTER BIT	AVDD CURRENT (MILLIAMPS)
BUFDCOPEN	0.1
PLLEN	1.4 (with clocks applied)
MICBEN	0.5
BIASEN	0.3
BUFIOEN	0.1
VMIDSEL	10K=>0.3, less than 0.1 for 100k/500k
INPPGAEN	0.2
ADCEN	x64 (ADCOSR=0)=>2.6, x128 (ADCOSR=1)=>4.9

Table 37 AVDD Supply Current

REGISTER MAP

ADDR B[15:9] DEC	HEX	REGISTER NAME	B8	B7	B6	B5	B4	B3	B2	B1	B0	DEF'T VAL (HEX)
0	00	Software Reset	Software reset									
1	01	Power manage't 1	BUFDCOPEN	0	AUXEN	PLLEN	MICBEN	BIASEN	BUFIOEN	VMIDSEL		000
2	02	Power manage't 2	0	0	0	0	BOOSTEN	0	INPPGAEN	0	ADCEN	000
4	04	Audio Interface	BCP	FRAMEP	WL		FMT		0	ALRSWAP	0	050
5	05	Companding ctrl	0	0	0	0	0		ADC_COMP		0	000
6	06	Clock Gen ctrl	CLKSEL	MCLKDIV			BCLKDIV			0	MS	140
7	07	Additional ctrl	0	0	0	0	0	SR			SLOWCLKEN	000
8	08	GPIO Stuff	0	0	0	OPCLKDIV		GPIOPOL	GPIOSEL			000
10	0A	DAC Control	0	0	0	DEEMPH		0	AMUTE	0	0	000
14	0E	ADC Control	HPFEN	HPFAPP	HPFCUT			ADCOSR128	0	0	ADCPOL	100
15	0F	ADC Digital Vol	0	ADCVOL								0FF
18	12	EQ1 – low shelf	0	0	EQ1C		EQ1G					12C
19	13	EQ2 – peak 1	EQ2BW	0	EQ2C		EQ2G					02C
20	14	EQ3 – peak 2	EQ3BW	0	EQ3C		EQ3G					02C
21	15	EQ4 – peak 3	EQ4BW	0	EQ4C		EQ4G					02C
22	16	EQ5 – high shelf	0	0	EQ5C		EQ5G					02C
27	1B	Notch Filter 1	NFU	NFEN	NFA0[13:7]							000
28	1C	Notch Filter 2	NFU	0	NFA0[6:0]							000
29	1D	Notch Filter 3	NFU	0	NFA1[13:7]							000
30	1E	Notch Filter 4	NFU	0	NFA1[6:0]							000
32	20	ALC control 1	ALCSEL	0	0	ALCMAX			ALCMIN			038
33	21	ALC control 2	ALCZC	ALCHLD				ALCLVL				00B
34	22	ALC control 3	ALCMODE	ALCDCY				ALCATK				032
35	23	Noise Gate	0	0	0	0	0	NGEN	NGTH			000
36	24	PLL N	0	0	0	0	PLL_PRESCALE	PLLN[3:0]				008
37	25	PLL K 1	0	0	0	PLLK[23:18]						00C
38	26	PLL K 2	PLLK[17:9]									093
39	27	PLL K 3	PLLK[8:0]									0E9
44	2C	Input ctrl	MBVSEL	0	0	0	0	AUXMODE	AUX2INPPGA	MICN2INPPGA	MICP2INPPGA	003
45	2D	INP PGA gain ctrl	0	INPPGAZC	INPPGAMUTE	INPPGAVOL						010
47	2F	ADC Boost ctrl	PGABOOST	0	MICP2BOOSTVOL			0	AUX2BOOSTVOL			100
49	31	Thermal Shutdown	0	0	0	0	0	0	0	TSDEN	0	002

DIGITAL FILTER CHARACTERISTICS

PARAMETER	TEST CONDITIONS	MIN	TYP	MAX	UNIT
ADC Filter					
Passband	+/- 0.025dB	0		0.454fs	
	-6dB		0.5fs		
Passband Ripple				+/- 0.025	dB
Stopband		0.546fs			
Stopband Attenuation	f > 0.546fs	-60			dB
Group Delay			21/fs		
ADC High Pass Filter					
High Pass Filter Corner Frequency	-3dB		3.7		Hz
	-0.5dB		10.4		
	-0.1dB		21.6		

Table 38 Digital Filter Characteristics

TERMINOLOGY

1. Stop Band Attenuation (dB) – the degree to which the frequency spectrum is attenuated (outside audio band)
2. Pass-band Ripple – any variation of the frequency response in the pass-band region

ADC FILTER RESPONSES

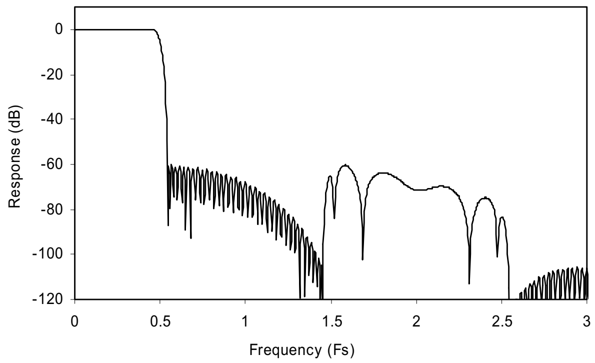


Figure 26 ADC Digital Filter Frequency Response

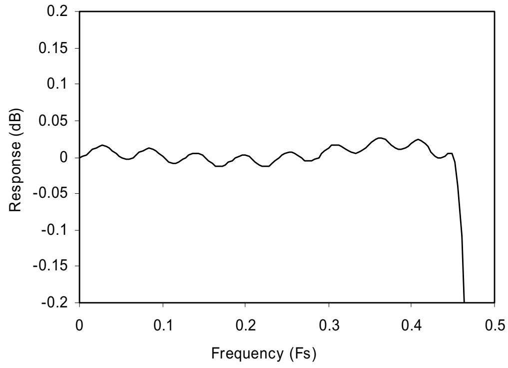


Figure 27 ADC Digital Filter Ripple

DE-EMPHASIS FILTER RESPONSES

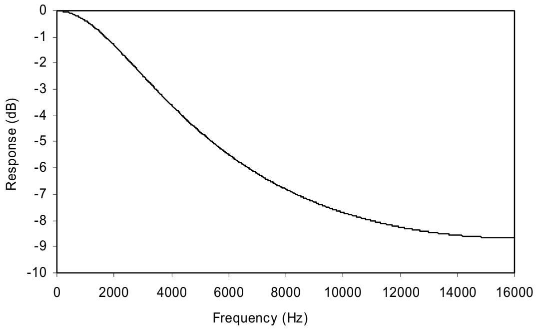


Figure 28 De-emphasis Frequency Response (32kHz)

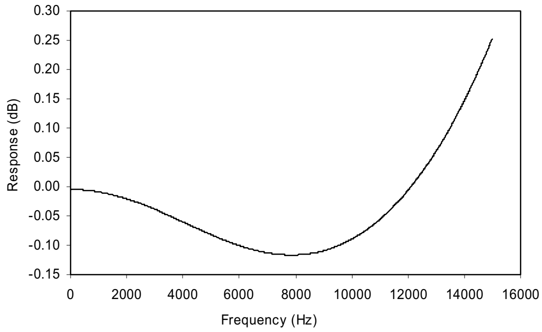


Figure 29 De-emphasis Error (32kHz)

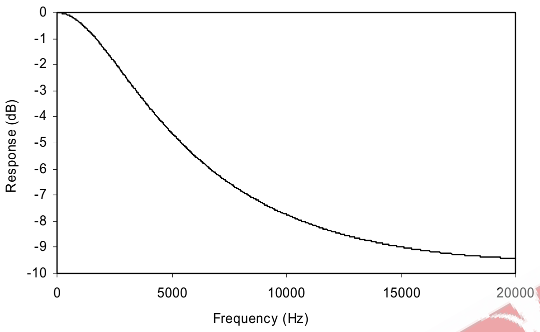


Figure 30 De-emphasis Frequency Response (44.1kHz)

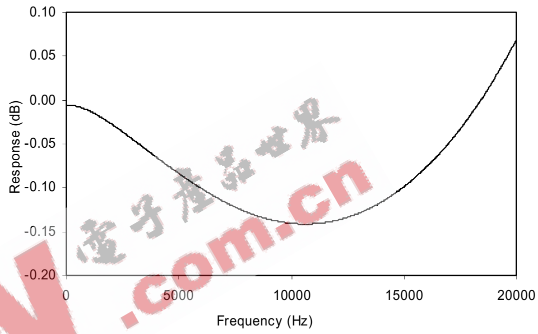


Figure 31 De-emphasis Error (44.1kHz)

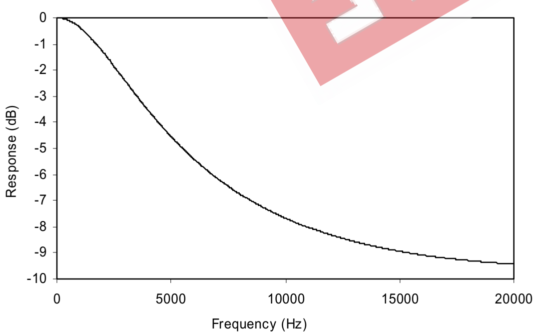


Figure 32 De-emphasis Frequency Response (48kHz)

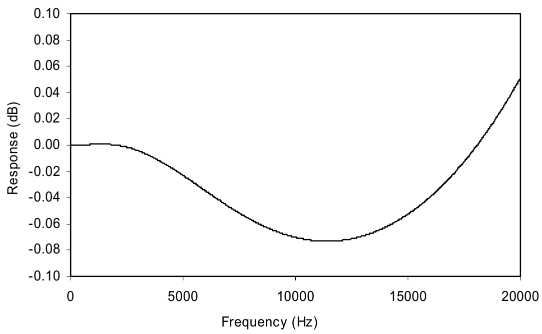


Figure 33 De-emphasis Error (48kHz)

HIGHPASS FILTER

The WM8950 has a selectable digital highpass filter in the ADC filter path. This filter has two modes, audio and applications. In audio mode the filter is a 1st order IIR with a cutoff of around 3.7Hz. In applications mode the filter is a 2nd order high pass filter with a selectable cutoff frequency.

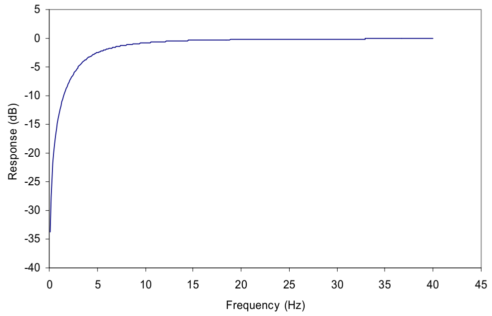


Figure 34 ADC Highpass Filter Response, HPFAPP=0

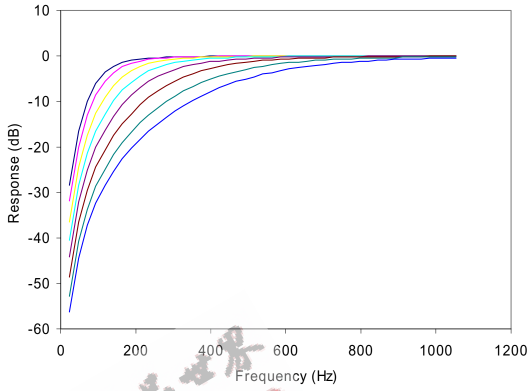


Figure 35 ADC Highpass Filter Responses (48kHz), HPFAPP=1, all cutoff settings shown.

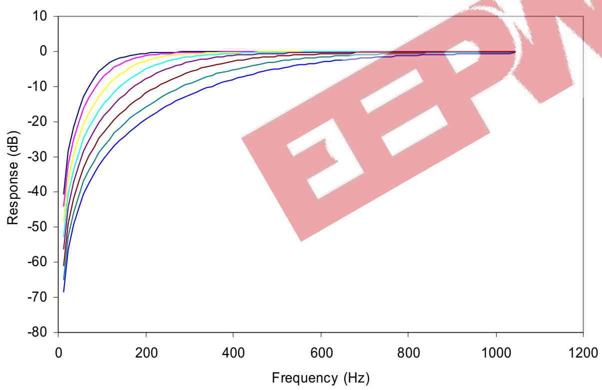


Figure 36 ADC Highpass Filter Responses (24kHz), HPFAPP=1, all cutoff settings shown.

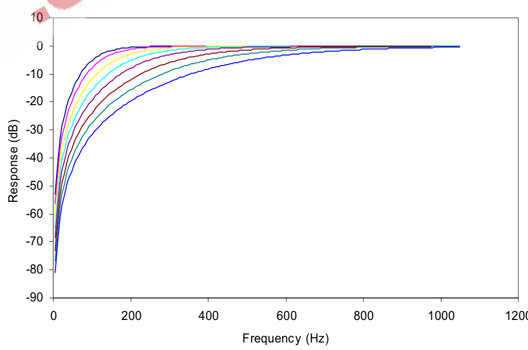


Figure 37 ADC Highpass Filter Responses (12kHz), HPFAPP=1, all cutoff settings shown.

5-BAND EQUALISER

The WM8950 has a 5-band equaliser which can be applied to the ADC path. The plots from Figure 38 to Figure 51 show the frequency responses of each filter with a sampling frequency of 48kHz, firstly showing the different cut-off/centre frequencies with a gain of ±12dB, and secondly a sweep of the gain from -12dB to +12dB for the lowest cut-off/centre frequency of each filter.

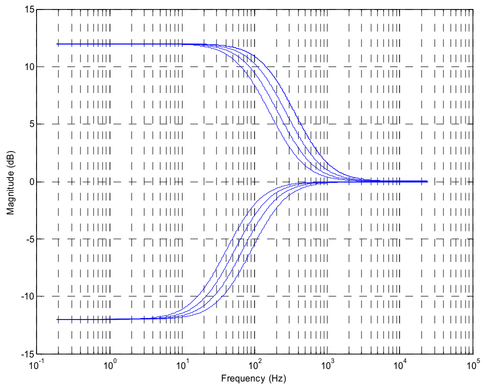


Figure 38 EQ Band 1 – Low Frequency Shelf Filter Cut-offs

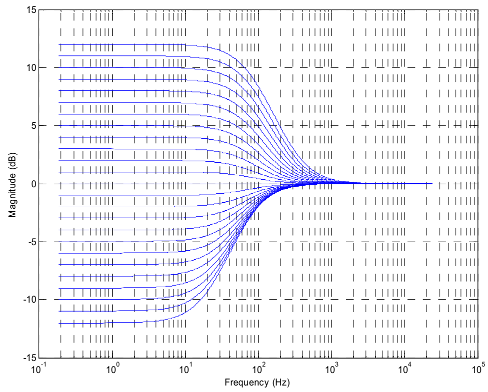


Figure 39 EQ Band 1 – Gains for Lowest Cut-off Frequency

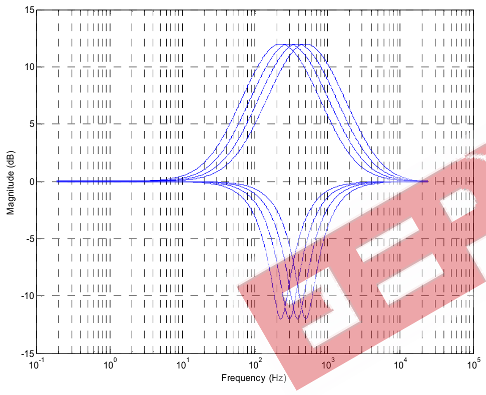


Figure 40 EQ Band 2 – Peak Filter Centre Frequencies, EQ2BW=0

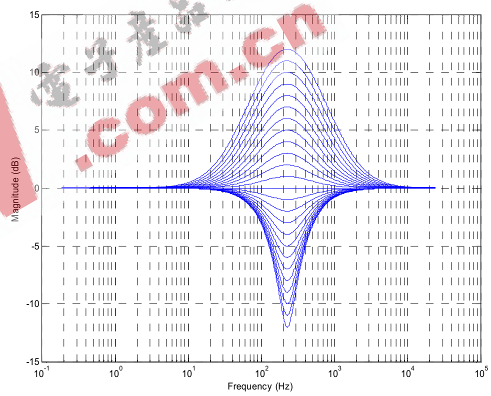


Figure 41 EQ Band 2 – Peak Filter Gains for Lowest Cut-off Frequency, EQ2BW=0

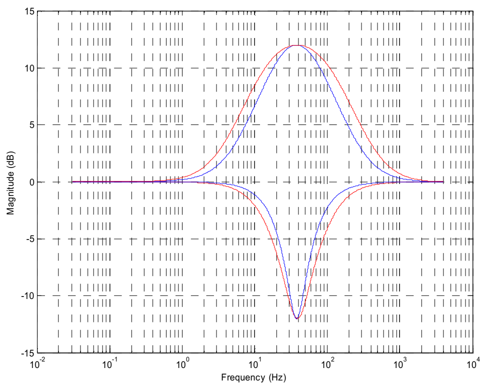


Figure 42 EQ Band 2 – EQ2BW=0, EQ2BW=1

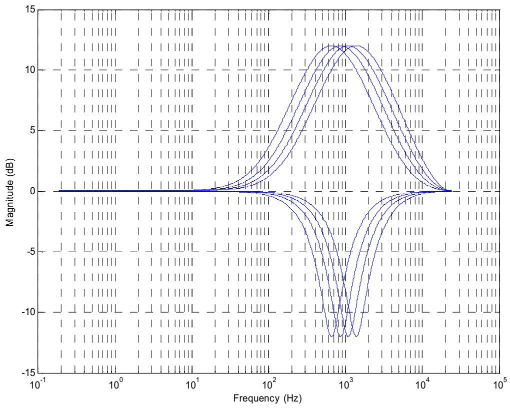


Figure 43 EQ Band 3 – Peak Filter Centre Frequencies, EQ3BW=0

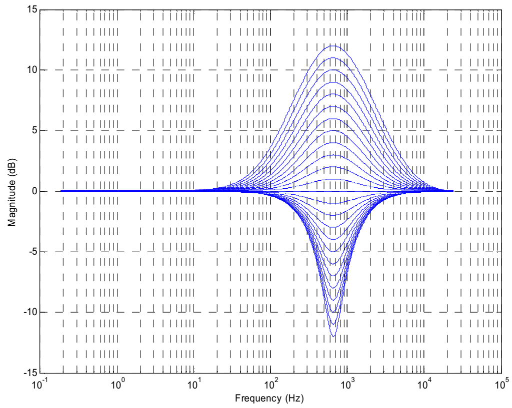


Figure 44 EQ Band 3 – Peak Filter Gains for Lowest Cut-off Frequency, EQ3BW=0

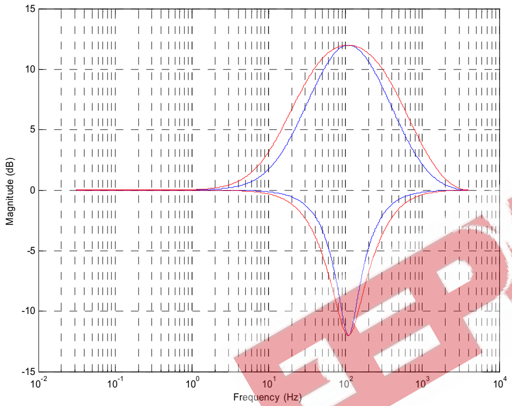


Figure 45 EQ Band 3 – EQ3BW=0, EQ3BW=1

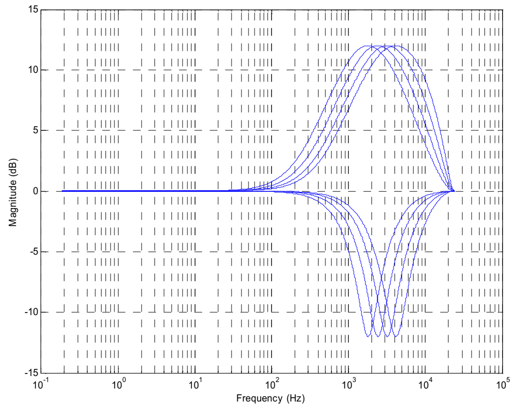


Figure 46 EQ Band 4 – Peak Filter Centre Frequencies, EQ3BW=0

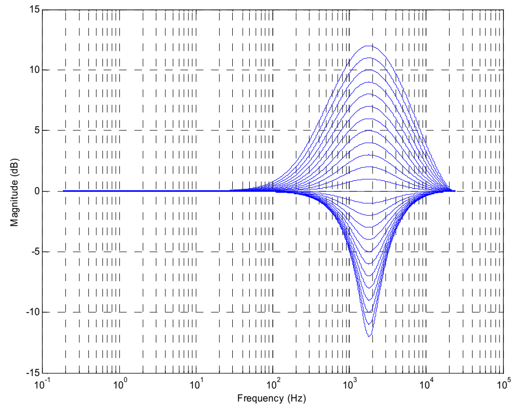


Figure 47 EQ Band 4 – Peak Filter Gains for Lowest Cut-off Frequency, EQ4BW=0

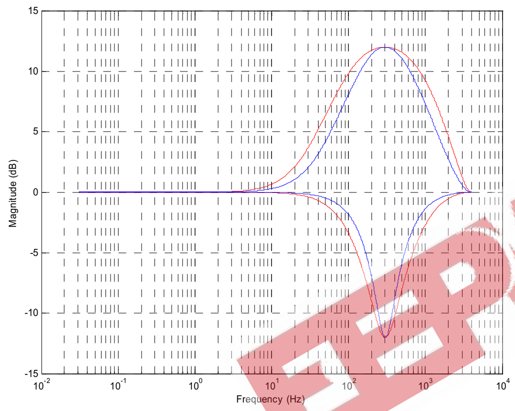


Figure 48 EQ Band 4 – EQ3BW=0, EQ3BW=1

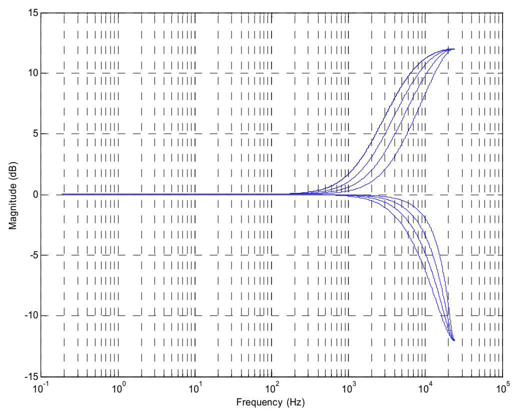


Figure 49 EQ Band 5 – High Frequency Shelf Filter Cut-offs

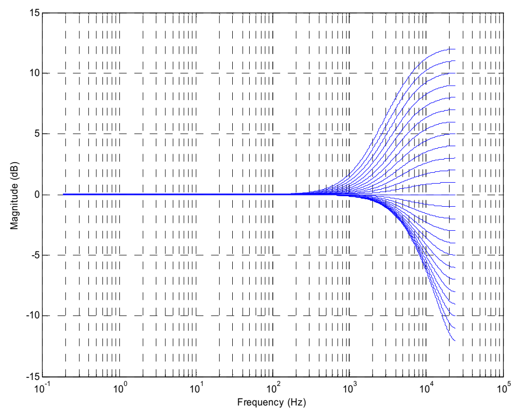


Figure 50 EQ Band 5 – Gains for Lowest Cut-off Frequency

Figure 51 shows the result of having the gain set on more than one channel simultaneously. The blue traces show each band (lowest cut-off/centre frequency) with ±12dB gain. The red traces show the cumulative effect of all bands with +12dB gain and all bands -12dB gain, with EQxBW=0 for the peak filters.

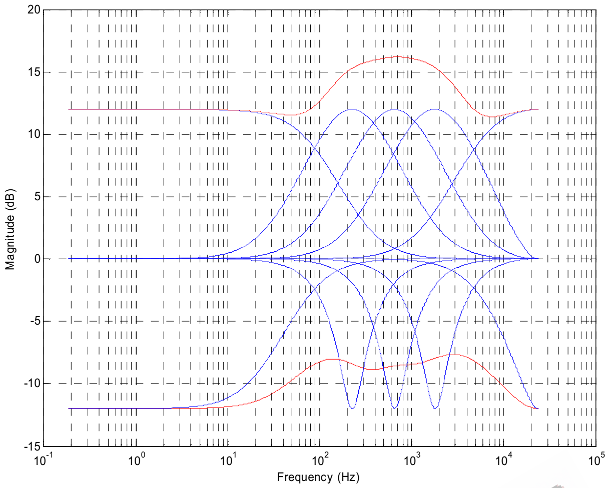
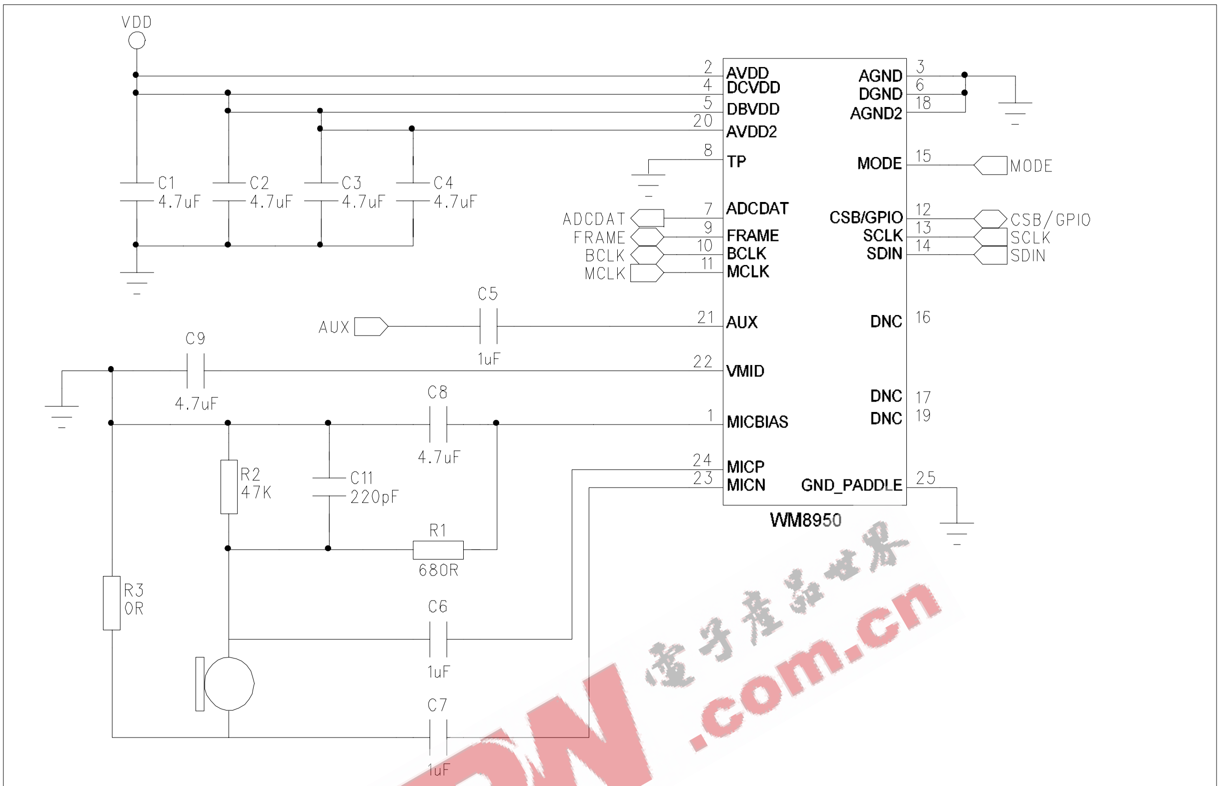


Figure 51 Cumulative Frequency Boost/Cut

APPLICATIONS INFORMATION

RECOMMENDED EXTERNAL COMPONENTS

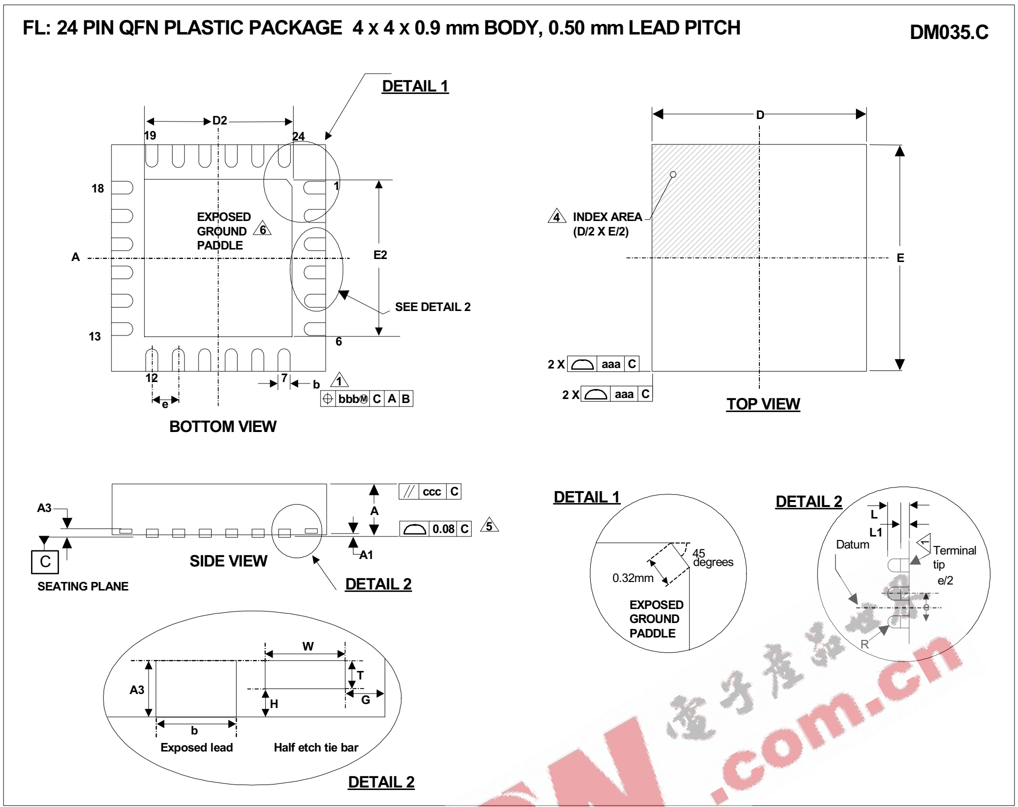


Notes:

1. AGND and DGND should be connected as close to the WM8950 as possible.
2. C1, C2, C3, C4, C8 and C9 should be positioned as close to WM8950 as possible.
3. Capacitor types should be carefully chosen. Capacitors with very low ESR are recommended for optimum performance.
4. R3 can be populated with other values to remove common mode noise on the microphone.
5. For added strength and heat dissipation, it is recommended that the GND_PADDLE (Pin 25) is connected to AGND.

Figure 52 Recommended External Components

PACKAGE DIAGRAM



Symbols	Dimensions (mm)			
	MIN	NOM	MAX	NOTE
A	0.80	0.90	1.00	
A1	0	0.02	0.05	
A3		0.20 REF		
b	0.18	0.25	0.30	1
D		4.00		
D2	2.00	2.15	2.25	2
E		4.00		
E2	2.00	2.15	2.25	2
e		0.50 BSC		
G		0.213		
H		0.1		
L	0.30	0.40	0.50	
L1	0.03		0.15	7
T		0.1		
W		0.2		
Tolerances of Form and Position				
aaa	0.15			
bbb	0.10			
ccc	0.10			
REF:	JEDEC, MO-220, VARIATION VGGD-2.			

NOTES:
1. DIMENSION b APPLIES TO METALLIZED TERMINAL AND IS MEASURED BETWEEN 0.15 mm AND 0.30 mm FROM TERMINAL TIP.
2. FALLS WITHIN JEDEC, MO-220, VARIATION VGGD-2.
3. ALL DIMENSIONS ARE IN MILLIMETRES.
4. THE TERMINAL #1 IDENTIFIER AND TERMINAL NUMBERING CONVENTION SHALL CONFORM TO JEDEC 95-1 SPP-002.
5. COPLANARITY APPLIES TO THE EXPOSED HEAT SINK SLUG AS WELL AS THE TERMINALS.
6. REFER TO APPLICATIONS NOTE WAN_0118 FOR FURTHER INFORMATION REGARDING PCB FOOTPRINTS AND QFN PACKAGE SOLDERING.
7. DEPENDING ON THE METHOD OF LEAD TERMINATION AT THE EDGE OF THE PACKAGE, PULL BACK (L1) MAY BE PRESENT.
8. THIS DRAWING IS SUBJECT TO CHANGE WITHOUT NOTICE.

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